

OPAx192 36-V, Precision, Rail-to-Rail Input/Output, Low Offset Voltage, Low Input Bias Current Op Amp with e-trim™

1 Features

- Low Offset Voltage: $\pm 5 \mu\text{V}$
- Low Offset Voltage Drift: $\pm 0.2 \mu\text{V}/^\circ\text{C}$
- Low Noise: $5.5 \text{ nV}/\sqrt{\text{Hz}}$ at 1 kHz
- High Common-Mode Rejection: 140 dB
- Low Bias Current: $\pm 5 \text{ pA}$
- Rail-to-Rail Input and Output
- Wide Bandwidth: 10 MHz GBW
- High Slew Rate: 20 V/ μs
- Low Quiescent Current: 1 mA per Amplifier
- Wide Supply: $\pm 2.25 \text{ V}$ to $\pm 18 \text{ V}$, $+4.5 \text{ V}$ to $+36 \text{ V}$
- EMI/RFI Filtered Inputs
- Differential Input Voltage Range to Supply Rail
- High Capacitive Load Drive Capability: 1 nF
- Industry Standard Packages:
 - Single in SOIC-8, SOT-5, and VSSOP-8
 - Dual in SOIC-8 and VSSOP-8
 - Quad in SOIC-14 and TSSOP-14

2 Applications

- Multiplexed Data-Acquisition Systems
- Test and Measurement Equipment
- High-Resolution ADC Driver Amplifiers
- SAR ADC Reference Buffers
- Programmable Logic Controllers
- High-Side and Low-Side Current Sensing
- High Precision Comparator

3 Description

The OPAx192 family (OPA192, OPA2192, and OPA4192) is a new generation of 36-V, e-trim operational amplifiers.

These devices offer outstanding dc precision and ac performance, including rail-to-rail input/output, low offset ($\pm 5 \mu\text{V}$, typ), low offset drift ($\pm 0.2 \mu\text{V}/^\circ\text{C}$, typ), and 10-MHz bandwidth.

Unique features such as differential input-voltage range to the supply rail, high output current ($\pm 65 \text{ mA}$), high capacitive load drive of up to 1 nF, and high slew rate (20 V/ μs) make the OPA192 a robust, high-performance operational amplifier for high-voltage industrial applications.

The OPA192 family of op amps is available in standard packages and is specified from -40°C to $+125^\circ\text{C}$.

Device Information⁽¹⁾

PART NUMBER	PACKAGE	BODY SIZE (NOM)
OPA192	SOIC (8)	4.90 mm x 3.90 mm
	SOT (5)	2.90 mm x 1.60 mm
	VSSOP (8)	3.00 mm x 3.00 mm
OPA2192	SOIC (8)	4.90 mm x 3.90 mm
	VSSOP (8)	3.00 mm x 3.00 mm
OPA4192 ⁽²⁾	SOIC (14)	8.65 mm x 3.90 mm
	TSSOP (14)	5.00 mm x 4.40 mm

(1) For all available packages, see the package option addendum at the end of the data sheet.

(2) OPA4192 is product preview.

OPA192 in a High-Voltage, Multiplexed, Data-Acquisition System

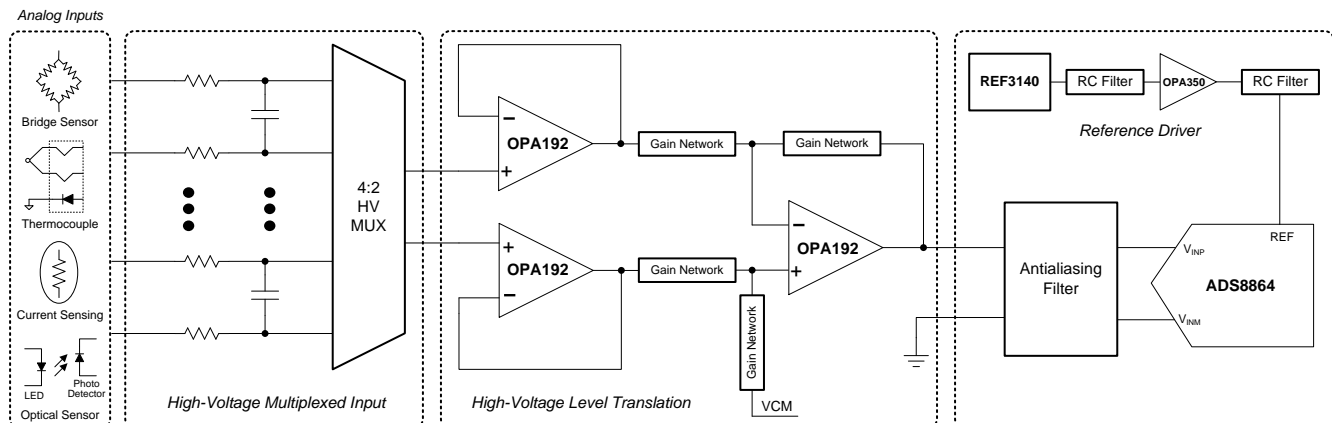


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4 Revision History

NOTE: Page numbers for previous revisions may differ from page numbers in the current version.

Changes from Revision B (March 2014) to Revision C	Page
• Added CDM row for OPA2192, OPA4192 in ESD Ratings table	6
• Changed input offset voltage values for $V_{CM} \geq (V+) - 1.5\text{ V}$ test condition	7
• Changed Input offset voltage parameter typical specs for $V_{CM} = (V+) - 1.5\text{ V}$ test conditions	7
• Changed test conditions for dV_{OS}/dT parameter	7
• Changed input offset voltage max values and test conditions for $V_{CM} = (V+) - 3\text{ V}$ test condition	9
• Changed input offset voltage values and test conditions for $V_{CM} = (V+) - 1.5\text{ V}$ test condition	9
• Changed Input offset voltage parameter typical specs for $V_{CM} = (V+) - 1.5\text{ V}$ test conditions	9
• Changed test conditions for dV_{OS}/dT parameter	9
• Added text to last bullet of <i>Layout Guidelines</i> section	34

Changes from Revision A (January 2014) to Revision B	Page
• Added ESD Ratings and Recommended Operating Conditions tables, and <i>Parameter Measurement Information</i> , <i>Application and Implementation</i> , <i>Power-Supply Recommendations</i> , and <i>Device and Documentation Support</i> sections, and moved existing sections	1
• Changed all OPA192 and OPA2192 packages to production data	1
• Changed package names to latest standard; changed all MSOP to VSSOP, SO to SOIC, and SOT23 to SOT	1
• Deleted DCK package pin configuration	4
• Added thermal information for OPA192 DBV and DGK packages	6
• Added OPA2192 and OPA4192 Thermal Information tables	7
• Added rows with additional test conditions to input offset voltage parameter	7
• Changed Input offset voltage drift parameter	7
• Changed CMRR test conditions	8
• Added rows with additional test conditions to input offset voltage parameter	9

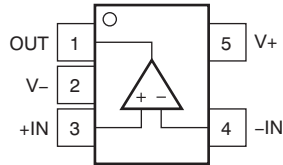
• Changed Input offset voltage drift parameter	9
• Changed PSSR parameter	9
• Changed CMRR test conditions	9
• Added <i>Output</i> section	10
• Added typical characteristic curves to Table 1	11
• Added $T_A = 25^\circ\text{C}$ to Typical Characteristics condition line	11
• Added nine new histogram plots from Figure 2 to Figure 10	12
• Changed Figure 11 to show more units	12
• Changed Figure 19	14
• Added text to Application Information section	30
• Changed text in Layout Guidelines section	34

Changes from Original (December 2013) to Revision A
Page

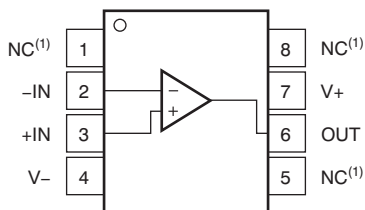
• Changed first paragraph of 16-Bit Precision Multiplexed Data-Acquisition System section	30
• Changed Figure 65 and title	30
• Changed TIDU181 reference design title	31

5 Pin Configuration and Functions

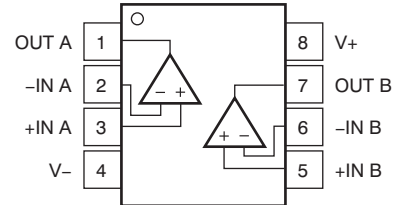
**DBV Package: OPA192
5-Pin SOT
(Top View)**



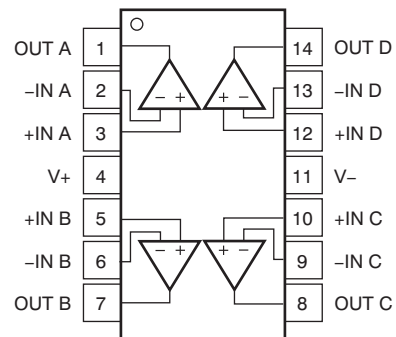
**D and DGK Packages: OPA192
8-Pin SOIC and VSSOP
(Top View)**



**D and DGK Packages: OPA2192
8-Pin SOIC and VSSOP
(Top View)**



**D and PW Packages: OPA4192⁽²⁾
14-Pin SOIC and TSSOP
(Top View)**



- (1) NC = No internal connection.
 (2) OPA4192 is product preview.

Pin Functions: OPA192

NAME	PIN		I/O	DESCRIPTION
	OPA192			
	D (SOIC), DGK (VSSOP)	DBV (SOT)		
+IN	3	3	I	Noninverting input
–IN	2	4	I	Inverting input
NC	1, 5, 8	—	—	No internal connection (can be left floating)
OUT	6	1	O	Output
V+	7	5	—	Positive (highest) power supply
V–	4	2	—	Negative (lowest) power supply

Pin Functions: OPA2192 and OPA4192

NAME	PIN		I/O	DESCRIPTION
	OPA2192	OPA4192		
	D (SOIC), DGK (VSSOP)	D (SOIC), PW (TSSOP)		
+IN A	3	3	I	Noninverting input, channel A
+IN B	5	5	I	Noninverting input, channel B
+IN C	—	10	I	Noninverting input, channel C
+IN D	—	12	I	Noninverting input, channel D
–IN A	2	2	I	Inverting input, channel A
–IN B	6	6	I	Inverting input, channel B
–IN C	—	9	I	Inverting input, channel C
–IN D	—	13	I	Inverting input, channel D
OUT A	1	1	O	Output, channel A
OUT B	7	7	O	Output, channel B
OUT C	—	8	O	Output, channel C
OUT D	—	14	O	Output, channel D
V+	8	4	—	Positive (highest) power supply
V–	4	11	—	Negative (lowest) power supply

6 Specifications

6.1 Absolute Maximum Ratings⁽¹⁾

over operating free-air temperature range (unless otherwise noted)

			MIN	MAX	UNIT
Supply voltage, $V_S = (V+) - (V-)$				± 20 (+40, single supply)	V
Signal input pins	Voltage	Common-mode	$(V-) - 0.5$	$(V+) + 0.5$	V
		Differential		$(V+) - (V-) + 0.2$	V
	Current		± 10	mA	
Output short circuit ⁽²⁾			Continuous		
Temperature	Operating range		-55	+150	°C
	Junction			150	°C
	Storage, T_{stg}		-65	+150	°C

- (1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
- (2) Short-circuit to ground, one amplifier per package.

6.2 ESD Ratings

			VALUE	UNIT
$V_{(ESD)}$	Electrostatic discharge	Human-body model (HBM), per ANSI/ESDA/JEDEC JS-001 ⁽¹⁾	± 4000	V
OPA192				
$V_{(ESD)}$	Electrostatic discharge	Charged-device model (CDM), per JEDEC specification JESD22-C101 ⁽²⁾	± 1000	V
OPA2192, OPA4192				
$V_{(ESD)}$	Electrostatic discharge	Charged-device model (CDM), per JEDEC specification JESD22-C101 ⁽²⁾	± 750	V

- (1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.
- (2) JEDEC document JEP157 states that 250-V CDM allows safe manufacturing with a standard ESD control process.

6.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted)

	MIN	NOM	MAX	UNIT
Supply voltage, $V_S = (V+) - (V-)$	4.5 (± 2.25)		36 (± 18)	V
Specified temperature	-40		+125	°C

6.4 Thermal Information: OPA192

THERMAL METRIC ⁽¹⁾		OPA192			UNIT
		D (SOIC)	DBV (SOT)	DGK (VSSOP)	
		8 PINS	5 PINS	8 PINS	
$R_{\theta JA}$	Junction-to-ambient thermal resistance	115.8	158.8	180.4	°C/W
$R_{\theta JC(top)}$	Junction-to-case(top) thermal resistance	60.1	60.7	67.9	
$R_{\theta JB}$	Junction-to-board thermal resistance	56.4	44.8	102.1	
Ψ_{JT}	Junction-to-top characterization parameter	12.8	1.6	10.4	
Ψ_{JB}	Junction-to-board characterization parameter	55.9	4.2	100.3	
$R_{\theta JC(bot)}$	Junction-to-case(bottom) thermal resistance	N/A	N/A	N/A	

- (1) For more information about traditional and new thermal metrics, see the *IC Package Thermal Metrics* application report, [SPRA953](http://www.ti.com/lit/zip/spra953).

6.5 Thermal Information: OPA2192

THERMAL METRIC ⁽¹⁾		OPA2192		UNIT
		D (SOIC)	DGK (VSSOP)	
		8 PINS	8 PINS	
R _{θJA}	Junction-to-ambient thermal resistance	107.9	158	°C/W
R _{θJC(top)}	Junction-to-case(top) thermal resistance	53.9	48.6	
R _{θJB}	Junction-to-board thermal resistance	48.9	78.7	
ψ _{JT}	Junction-to-top characterization parameter	6.6	3.9	
ψ _{JB}	Junction-to-board characterization parameter	48.3	77.3	
R _{θJC(bot)}	Junction-to-case(bottom) thermal resistance	N/A	N/A	

(1) For more information about traditional and new thermal metrics, see the *IC Package Thermal Metrics* application report, [SPRA953](#).

6.6 Thermal Information: OPA4192

THERMAL METRIC ⁽¹⁾		OPA4192		UNIT
		D (SOIC)	PW (TSSOP)	
		14 PINS	14 PINS	
R _{θJA}	Junction-to-ambient thermal resistance	86.4	92.6	°C/W
R _{θJC(top)}	Junction-to-case(top) thermal resistance	46.3	27.5	
R _{θJB}	Junction-to-board thermal resistance	41.0	33.6	
ψ _{JT}	Junction-to-top characterization parameter	11.3	1.9	
ψ _{JB}	Junction-to-board characterization parameter	40.7	33.1	
R _{θJC(bot)}	Junction-to-case(bottom) thermal resistance	N/A	N/A	

(1) For more information about traditional and new thermal metrics, see the *IC Package Thermal Metrics* application report, [SPRA953](#).

6.7 Electrical Characteristics: V_S = ±4 V to ±18 V (V_S = +8 V to +36 V)

At T_A = +25°C, V_{CM} = V_{OUT} = V_S / 2, and R_{LOAD} = 10 kΩ connected to V_S / 2, unless otherwise noted.

PARAMETER	TEST CONDITIONS		MIN	TYP	MAX	UNIT
OFFSET VOLTAGE						
V _{OS}	Input offset voltage			±5	±25	μV
		T _A = 0°C to 85°C		±8	±50	μV
		T _A = -40°C to +125°C		±10	±75	μV
		V _{CM} = (V+) - 1.5 V		±10	±40	μV
			T _A = 0°C to 85°C	±25	±150	μV
			T _A = -40°C to +125°C	±50	±250	μV
dV _{OS} /dT	D packages only	T _A = 0°C to 85°C	±0.1	±0.5	μV/°C	
		T _A = -40°C to +125°C	±0.15	±0.8	μV/°C	
	DBV and DGK packages only	T _A = 0°C to 85°C	±0.1	±0.8	μV/°C	
		T _A = -40°C to +125°C	±0.2	±1.0	μV/°C	
PSRR	Power-supply rejection ratio	T _A = -40°C to +125°C		±0.3	±1.0	μV/V
INPUT BIAS CURRENT						
I _B	Input bias current			±5	±20	pA
		T _A = -40°C to +125°C			±5	nA
I _{OS}	Input offset current			±2	±20	pA
		T _A = -40°C to +125°C			±2	nA
NOISE						
E _n	Input voltage noise	(V-) - 0.1 V < V _{CM} < (V+) - 3 V	f = 0.1 Hz to 10 Hz	1.30		μV _{PP}
		(V+) - 1.5 V < V _{CM} < (V+) + 0.1 V	f = 0.1 Hz to 10 Hz	4		μV _{PP}
e _n	Input voltage noise density	(V-) - 0.1 V < V _{CM} < (V+) - 3 V	f = 100 Hz	10.5		nV/√Hz
			f = 1 kHz	5.5		nV/√Hz
		(V+) - 1.5 V < V _{CM} < (V+) + 0.1 V	f = 100 Hz	32		nV/√Hz
			f = 1 kHz	12.5		nV/√Hz

Electrical Characteristics: $V_S = \pm 4\text{ V}$ to $\pm 18\text{ V}$ ($V_S = +8\text{ V}$ to $+36\text{ V}$) (continued)

 At $T_A = +25^\circ\text{C}$, $V_{CM} = V_{OUT} = V_S / 2$, and $R_{LOAD} = 10\text{ k}\Omega$ connected to $V_S / 2$, unless otherwise noted.

PARAMETER		TEST CONDITIONS		MIN	TYP	MAX	UNIT
NOISE (continued)							
i_n	Input current noise density	$f = 1\text{ kHz}$			1.5		fA/ $\sqrt{\text{Hz}}$
INPUT VOLTAGE							
V_{CM}	Common-mode voltage range			(V-) - 0.1		(V+) + 0.1	V
CMRR	Common-mode rejection ratio	(V-) - 0.1 V < V_{CM} < (V+) - 3 V		120	140		dB
			$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$	114	126		dB
		(V+) - 1.5 V < V_{CM} < (V+)		100	120		dB
			$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$	86	100		dB
		(V+) - 3 V < V_{CM} < (V+) - 1.5 V		See Typical Characteristics			
INPUT IMPEDANCE							
Z_{ID}	Differential			100 1.6			M Ω pF
Z_{IC}	Common-mode			1 6.4			$10^{13}\Omega$ pF
OPEN-LOOP GAIN							
A_{OL}	Open-loop voltage gain	(V-) + 0.6 V < V_O < (V+) - 0.6 V, $R_{LOAD} = 2\text{ k}\Omega$		120	134		dB
			$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$	114	126		dB
		(V-) + 0.3 V < V_O < (V+) - 0.3 V, $R_{LOAD} = 10\text{ k}\Omega$		126	140		dB
			$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$	120	134		dB
FREQUENCY RESPONSE							
GBW	Unity gain bandwidth			10			MHz
SR	Slew rate	$G = 1$, 10-V step		20			V/ μs
t_s	Settling time	To 0.01%	$V_S = \pm 18\text{ V}$, $G = 1$, 10-V step	1.4			μs
			$V_S = \pm 18\text{ V}$, $G = 1$, 5-V step	0.9			μs
		To 0.001%	$V_S = \pm 18\text{ V}$, $G = 1$, 10-V step	2.1			μs
			$V_S = \pm 18\text{ V}$, $G = 1$, 5-V step	1.8			μs
t_{OR}	Overload recovery time	$V_{IN} \times G = V_S$		200			ns
THD+N	Total harmonic distortion + noise	$G = 1$, $f = 1\text{ kHz}$, $V_O = 3.5\text{ V}_{RMS}$		0.00008%			
OUTPUT							
V_O	Voltage output swing from rail	Positive rail	No load	5	15		mV
			$R_{LOAD} = 10\text{ k}\Omega$	95	110		mV
			$R_{LOAD} = 2\text{ k}\Omega$	430	500		mV
		Negative rail	No load	5	15		mV
			$R_{LOAD} = 10\text{ k}\Omega$	95	110		mV
			$R_{LOAD} = 2\text{ k}\Omega$	430	500		mV
I_{SC}	Short-circuit current			± 65			mA
C_{LOAD}	Capacitive load drive			See Typical Characteristics			
Z_O	Open-loop output impedance	$f = 1\text{ MHz}$, $I_O = 0\text{ A}$, See Figure 31		375			Ω
POWER SUPPLY							
I_Q	Quiescent current per amplifier	$I_O = 0\text{ A}$		1	1.2		mA
		$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$, $I_O = 0\text{ A}$		1.5			mA
TEMPERATURE							
	Thermal protection ⁽¹⁾			140			$^\circ\text{C}$

 (1) For a detailed description of thermal protection, see the [Thermal Protection](#) section.

6.8 Electrical Characteristics: $V_S = \pm 2.25\text{ V}$ to $\pm 4\text{ V}$ ($V_S = +4.5\text{ V}$ to $+8\text{ V}$)

At $T_A = +25^\circ\text{C}$, $V_{CM} = V_{OUT} = V_S / 2$, and $R_{LOAD} = 10\text{ k}\Omega$ connected to $V_S / 2$, unless otherwise noted.

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT	
OFFSET VOLTAGE						
V_{OS}	Input offset voltage	$V_{CM} = (V+) - 3\text{ V}$	$T_A = 0^\circ\text{C}$ to 85°C	± 5	± 25	μV
			$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$	± 8	± 50	μV
	$(V+) - 3.5\text{ V} < V_{CM} < (V+) - 1.5\text{ V}$		See Common-Mode Voltage Range section			
	$V_{CM} = (V+) - 1.5\text{ V}$	$T_A = 0^\circ\text{C}$ to 85°C	± 10	± 40	μV	
$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$		± 25	± 150	μV		
dV_{OS}/dT	Input offset voltage drift	$V_{CM} = (V+) - 3\text{ V}$, D packages only	$T_A = 0^\circ\text{C}$ to 85°C	± 0.1	± 0.5	$\mu\text{V}/^\circ\text{C}$
			$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$	± 0.15	± 0.8	$\mu\text{V}/^\circ\text{C}$
	$V_{CM} = (V+) - 3\text{ V}$, DBV and DGK packages only	$T_A = 0^\circ\text{C}$ to 85°C	± 0.1	± 0.8	$\mu\text{V}/^\circ\text{C}$	
		$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$	± 0.2	± 1.1	$\mu\text{V}/^\circ\text{C}$	
$V_{CM} = (V+) - 1.5\text{ V}$, $T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$		± 0.5	± 3	$\mu\text{V}/^\circ\text{C}$		
PSRR	Power-supply rejection ratio	$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$, $V_{CM} = V_S / 2 - 0.75\text{ V}$		± 1	$\mu\text{V}/\text{V}$	
INPUT BIAS CURRENT						
I_B	Input bias current			± 5	± 20	pA
		$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$			± 5	nA
I_{OS}	Input offset current			± 2	± 20	pA
		$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$			± 2	nA
NOISE						
E_n	Input voltage noise	$(V-) - 0.1\text{ V} < V_{CM} < (V+) - 3\text{ V}$, $f = 0.1\text{ Hz}$ to 10 Hz		1.30		μV_{PP}
		$(V+) - 1.5\text{ V} < V_{CM} < (V+) + 0.1\text{ V}$, $f = 0.1\text{ Hz}$ to 10 Hz		4		μV_{PP}
e_n	Input voltage noise density	$(V-) - 0.1\text{ V} < V_{CM} < (V+) - 3\text{ V}$	$f = 100\text{ Hz}$	10.5		$\text{nV}/\sqrt{\text{Hz}}$
			$f = 1\text{ kHz}$	5.5		$\text{nV}/\sqrt{\text{Hz}}$
		$(V+) - 1.5\text{ V} < V_{CM} < (V+) + 0.1\text{ V}$	$f = 100\text{ Hz}$	32		$\text{nV}/\sqrt{\text{Hz}}$
			$f = 1\text{ kHz}$	12.5		$\text{nV}/\sqrt{\text{Hz}}$
i_n	Input current noise density	$f = 1\text{ kHz}$		1.5		$\text{fA}/\sqrt{\text{Hz}}$
INPUT VOLTAGE						
V_{CM}	Common-mode voltage range			$(V-) - 0.1$	$(V+) + 0.1$	V
CMRR	Common-mode rejection ratio	$(V-) - 0.1\text{ V} < V_{CM} < (V+) - 3\text{ V}$	$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$	94	110	dB
				90	104	dB
		$(V+) - 1.5\text{ V} < V_{CM} < (V+)$	$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$	100	120	dB
				84	100	dB
$(V+) - 3\text{ V} < V_{CM} < (V+) - 1.5\text{ V}$		See Typical Characteristics				
INPUT IMPEDANCE						
Z_{ID}	Differential			100 1.6		$\text{M}\Omega$ pF
Z_{IC}	Common-mode			1 6.4		$10^{13}\Omega$ pF
OPEN-LOOP GAIN						
A_{OL}	Open-loop voltage gain	$(V-) + 0.6\text{ V} < V_O < (V+) - 0.6\text{ V}$, $R_{LOAD} = 2\text{ k}\Omega$	$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$	110	120	dB
				100	114	dB
		$(V-) + 0.3\text{ V} < V_O < (V+) - 0.3\text{ V}$, $R_{LOAD} = 10\text{ k}\Omega$	$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$	110	126	dB
				110	120	dB

Electrical Characteristics: $V_S = \pm 2.25\text{ V}$ to $\pm 4\text{ V}$ ($V_S = +4.5\text{ V}$ to $+8\text{ V}$) (continued)

 At $T_A = +25^\circ\text{C}$, $V_{CM} = V_{OUT} = V_S / 2$, and $R_{LOAD} = 10\text{ k}\Omega$ connected to $V_S / 2$, unless otherwise noted.

PARAMETER		TEST CONDITIONS		MIN	TYP	MAX	UNIT
FREQUENCY RESPONSE							
GBW	Unity gain bandwidth				10		MHz
SR	Slew rate	G = 1, 10-V step			20		V/ μs
t_s	Settling time	To 0.01%	$V_S = \pm 3\text{ V}$, G = 1, 5-V step		1		μs
t_{OR}	Overload recovery time	$V_{IN} \times G = V_S$			200		ns
OUTPUT							
V_O	Voltage output swing from rail	Positive rail	No load		5	15	mV
			$R_{LOAD} = 10\text{ k}\Omega$		95	110	mV
			$R_{LOAD} = 2\text{ k}\Omega$		430	500	mV
		Negative rail	No load		5	15	mV
			$R_{LOAD} = 10\text{ k}\Omega$		95	110	mV
			$R_{LOAD} = 2\text{ k}\Omega$		430	500	mV
I_{SC}	Short-circuit current				± 65		mA
C_{LOAD}	Capacitive load drive			See Typical Characteristics			
Z_O	Open-loop output impedance	f = 1 MHz, $I_O = 0\text{ A}$, see Figure 31			375		Ω
POWER SUPPLY							
I_Q	Quiescent current per amplifier	$I_O = 0\text{ A}$			1	1.2	mA
				$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$		1.5	mA
TEMPERATURE							
	Thermal protection ⁽¹⁾				140		$^\circ\text{C}$

 (1) For a detailed description of thermal protection, see the [Thermal Protection](#) section.

6.9 Typical Characteristics

Table 1. Table of Graphs

DESCRIPTION	FIGURE
Offset Voltage Production Distribution	Figure 1 , Figure 3 , Figure 2 , Figure 6 , Figure 5 , Figure 4
Offset Voltage Drift Distribution	Figure 7 , Figure 8 , Figure 9 , Figure 10
Offset Voltage vs Temperature	Figure 11
Offset Voltage vs Common-Mode Voltage	Figure 12 , Figure 13 , Figure 14
Offset Voltage vs Power Supply	Figure 15
Open-Loop Gain and Phase vs Frequency	Figure 16
Closed-Loop Gain and Phase vs Frequency	Figure 17
Input Bias Current vs Common-Mode Voltage	Figure 18
Input Bias Current vs Temperature	Figure 19
Output Voltage Swing vs Output Current (maximum supply)	Figure 20
CMRR and PSRR vs Frequency	Figure 21
CMRR vs Temperature	Figure 22
PSRR vs Temperature	Figure 23
0.1-Hz to 10-Hz Noise	Figure 24
Input Voltage Noise Spectral Density vs Frequency	Figure 25
THD+N Ratio vs Frequency	Figure 26
THD+N vs Output Amplitude	Figure 27
Quiescent Current vs Supply Voltage	Figure 28
Quiescent Current vs Temperature	Figure 29
Open Loop Gain vs Temperature	Figure 30
Open Loop Output Impedance vs Frequency	Figure 31
Small Signal Overshoot vs Capacitive Load (100-mV output step)	Figure 32 , Figure 33
No Phase Reversal	Figure 34
Positive Overload Recovery	Figure 35
Negative Overload Recovery	Figure 36
Small-Signal Step Response (100 mV)	Figure 37 , Figure 38
Large-Signal Step Response	Figure 39
Settling Time	Figure 40 , Figure 41 , Figure 42 , Figure 43
Short-Circuit Current vs Temperature	Figure 44
Maximum Output Voltage vs Frequency	Figure 45
Propagation Delay Rising Edge	Figure 46
Propagation Delay Falling Edge	Figure 47

At $T_A = 25^\circ\text{C}$, $V_S = \pm 18\text{ V}$, $V_{CM} = V_S / 2$, $R_{LOAD} = 10\text{ k}\Omega$ connected to $V_S / 2$, and $C_L = 100\text{ pF}$, unless otherwise noted.

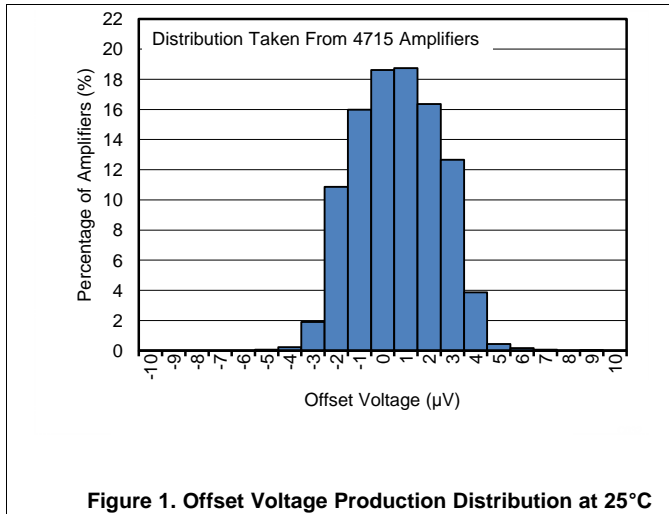


Figure 1. Offset Voltage Production Distribution at 25°C

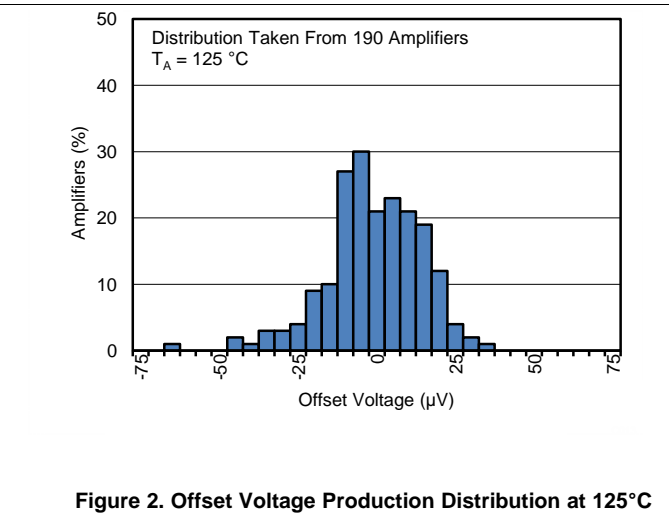


Figure 2. Offset Voltage Production Distribution at 125°C

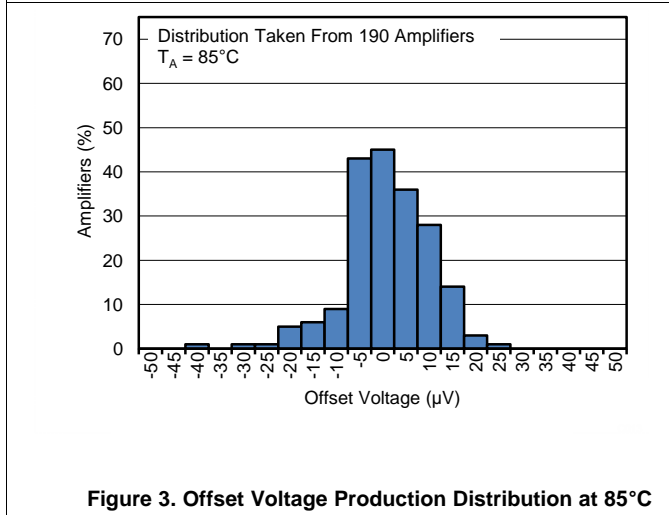


Figure 3. Offset Voltage Production Distribution at 85°C

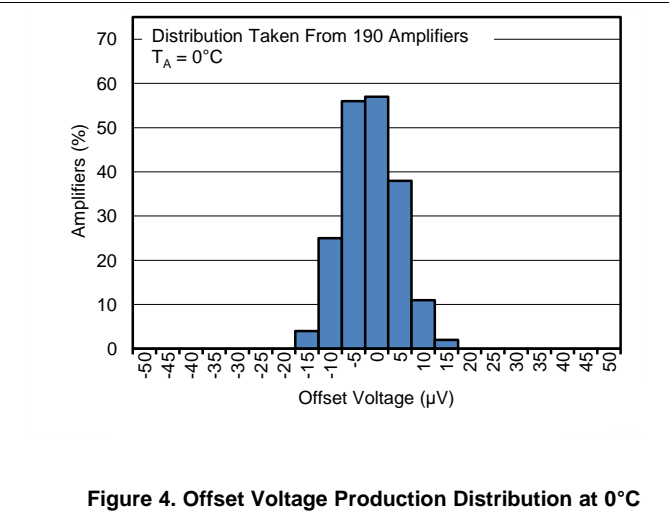


Figure 4. Offset Voltage Production Distribution at 0°C

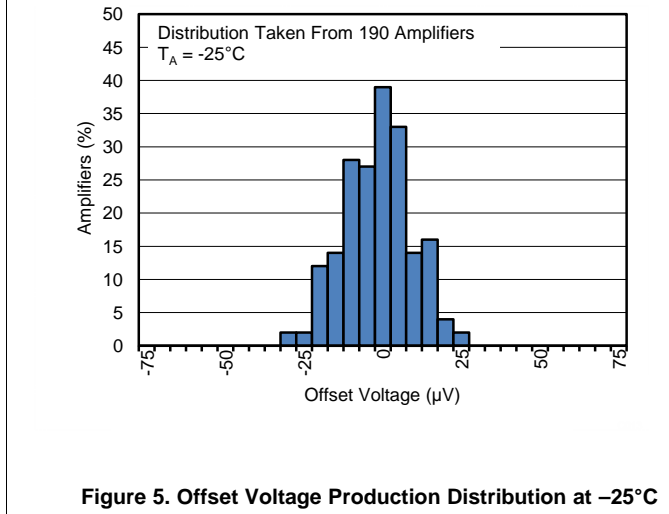


Figure 5. Offset Voltage Production Distribution at -25°C

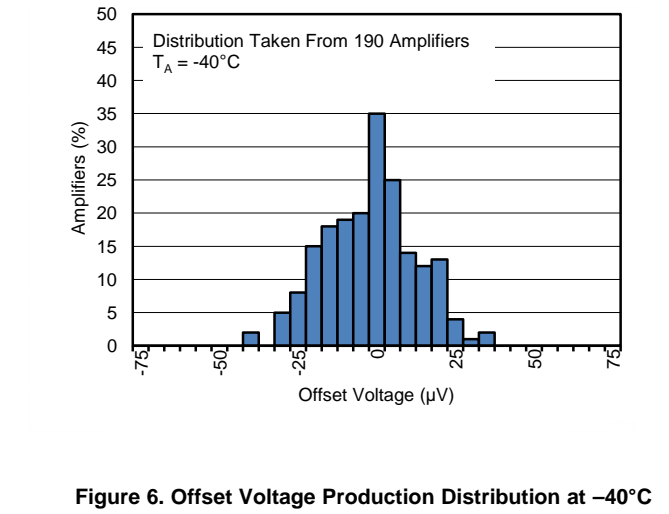


Figure 6. Offset Voltage Production Distribution at -40°C

At $T_A = 25^\circ\text{C}$, $V_S = \pm 18\text{ V}$, $V_{CM} = V_S / 2$, $R_{LOAD} = 10\text{ k}\Omega$ connected to $V_S / 2$, and $C_L = 100\text{ pF}$, unless otherwise noted.

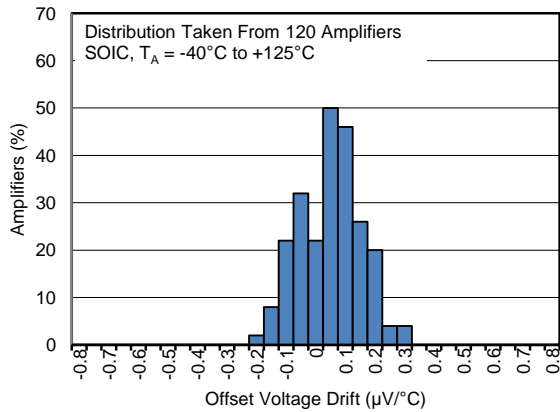


Figure 7. Offset Voltage Drift Distribution from -40°C to $+125^\circ\text{C}$ (OPA192ID and OPA2192ID)

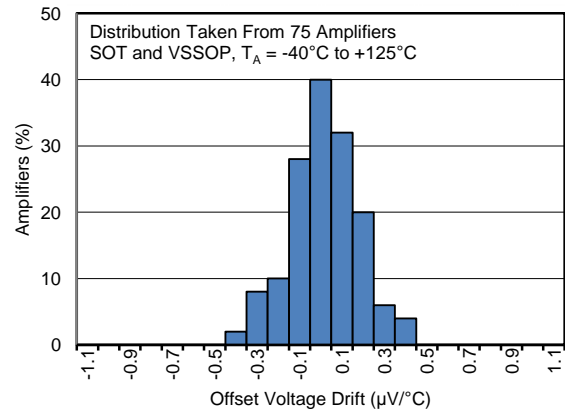


Figure 8. Offset Voltage Drift Distribution from -40°C to $+125^\circ\text{C}$ (OPA192IDBV, OPA192IDGK and OPA2192IDGK)

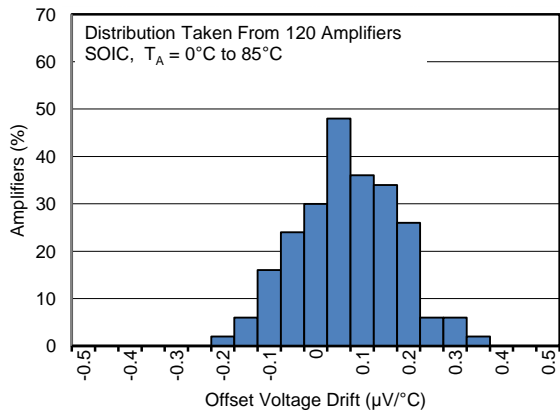


Figure 9. Offset Voltage Drift Distribution from 0°C to 85°C (OPA192ID and OPA2192ID)

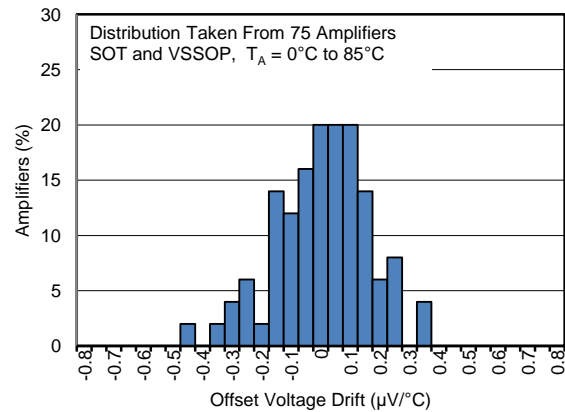


Figure 10. Offset Voltage Drift Distribution from 0°C to 85°C (OPA192IDBV, OPA192IDGK and OPA2192IDGK)

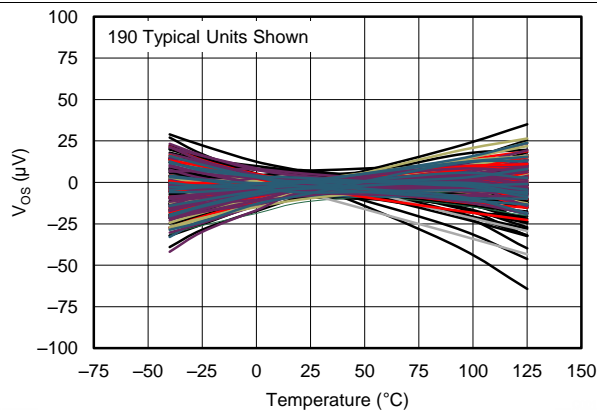


Figure 11. Offset Voltage vs Temperature

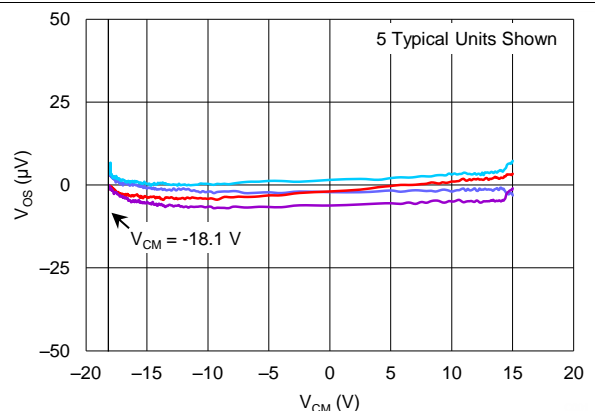


Figure 12. Offset Voltage vs Common-Mode Voltage

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At $T_A = 25^\circ\text{C}$, $V_S = \pm 18\text{ V}$, $V_{CM} = V_S / 2$, $R_{LOAD} = 10\text{ k}\Omega$ connected to $V_S / 2$, and $C_L = 100\text{ pF}$, unless otherwise noted.

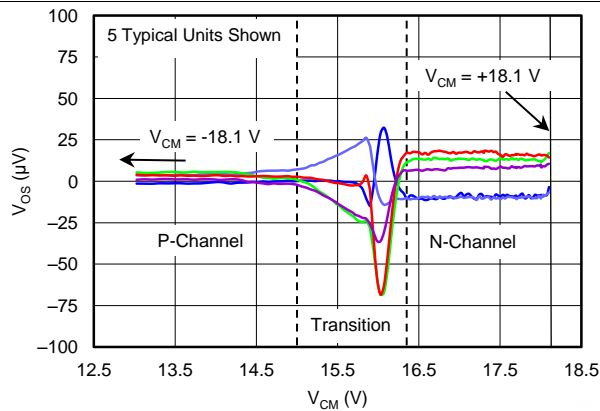


Figure 13. Offset Voltage vs Common-Mode Voltage

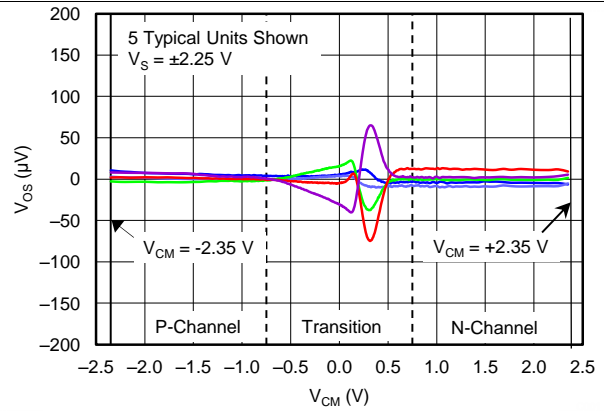


Figure 14. Offset Voltage vs Common-Mode Voltage

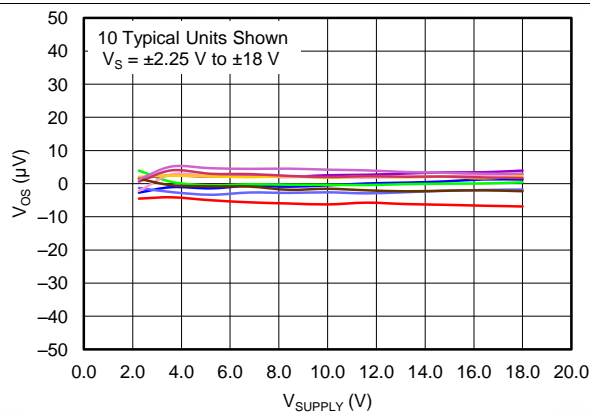


Figure 15. Offset Voltage vs Power Supply

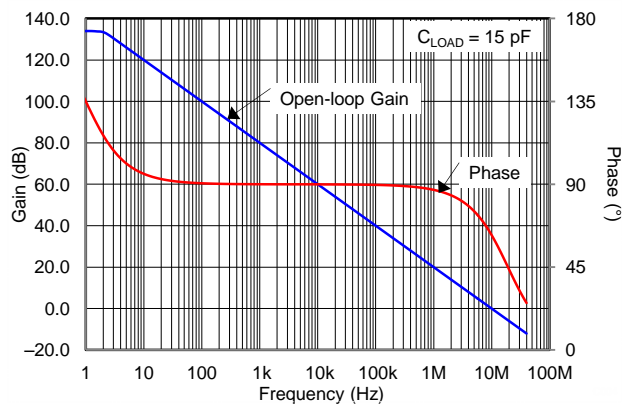


Figure 16. Open-Loop Gain and Phase vs Frequency

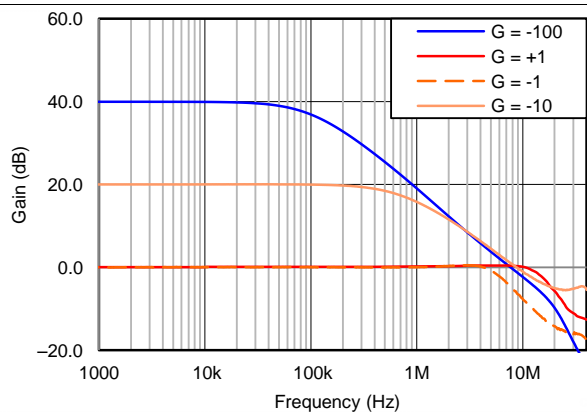


Figure 17. Closed-Loop Gain and Phase vs Frequency

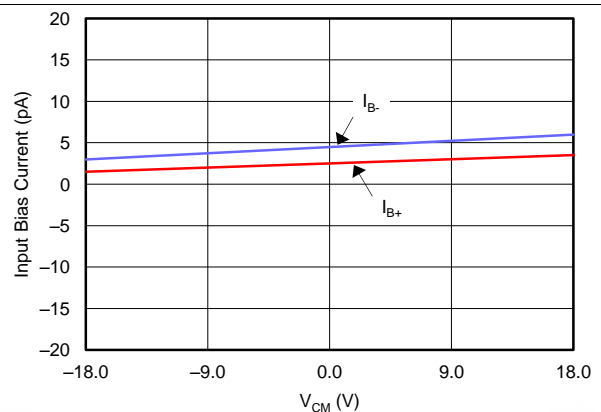


Figure 18. Input Bias Current vs Common-Mode Voltage

At $T_A = 25^\circ\text{C}$, $V_S = \pm 18\text{ V}$, $V_{CM} = V_S / 2$, $R_{LOAD} = 10\text{ k}\Omega$ connected to $V_S / 2$, and $C_L = 100\text{ pF}$, unless otherwise noted.

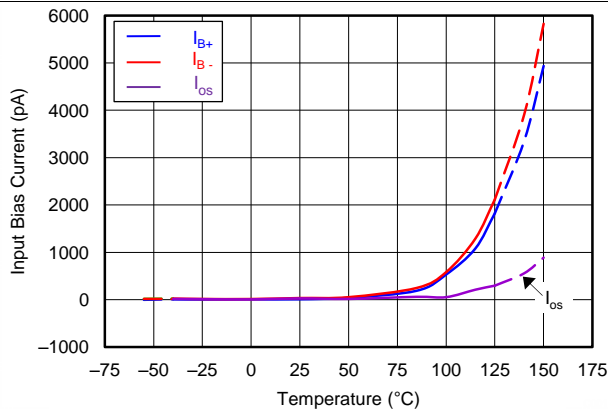


Figure 19. Input Bias Current vs Temperature

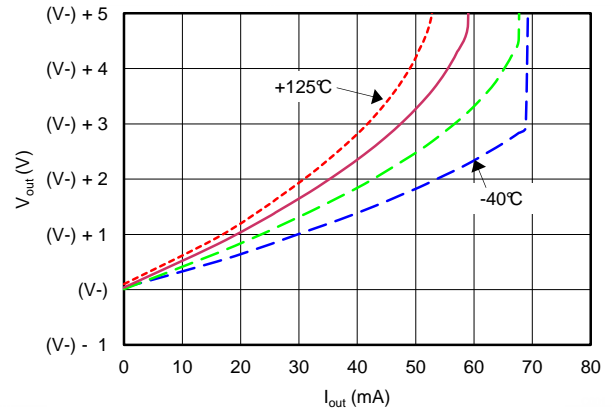


Figure 20. Output Voltage Swing vs Output Current (Maximum Supply)

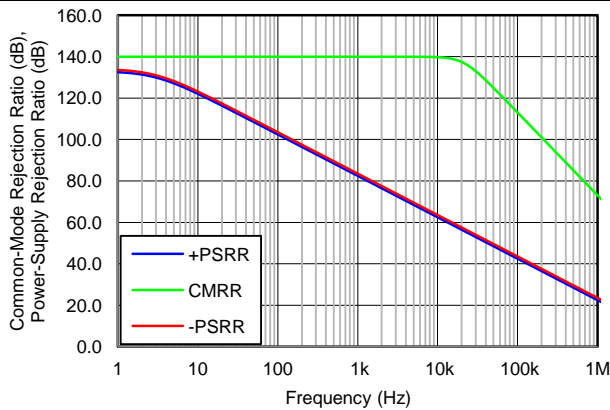


Figure 21. CMRR and PSRR vs Frequency

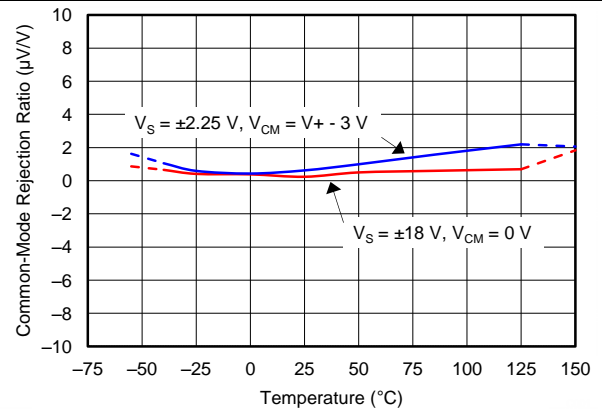


Figure 22. CMRR vs Temperature

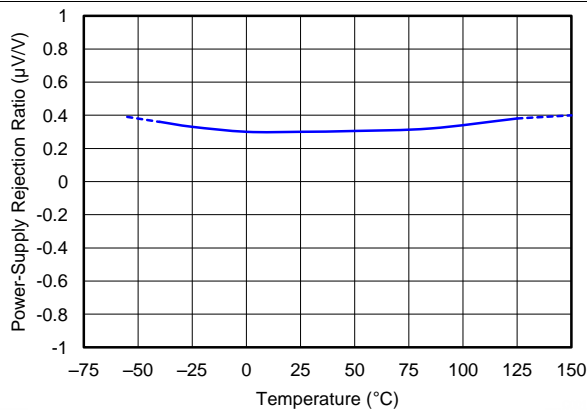


Figure 23. PSRR vs Temperature

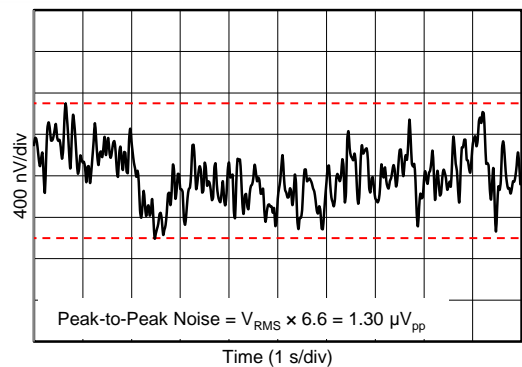


Figure 24. 0.1-Hz to 10-Hz Noise

At $T_A = 25^\circ\text{C}$, $V_S = \pm 18\text{ V}$, $V_{CM} = V_S / 2$, $R_{LOAD} = 10\text{ k}\Omega$ connected to $V_S / 2$, and $C_L = 100\text{ pF}$, unless otherwise noted.

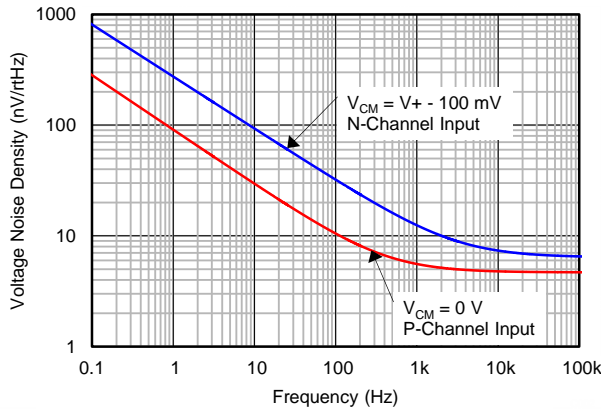


Figure 25. Input Voltage Noise Spectral Density vs Frequency

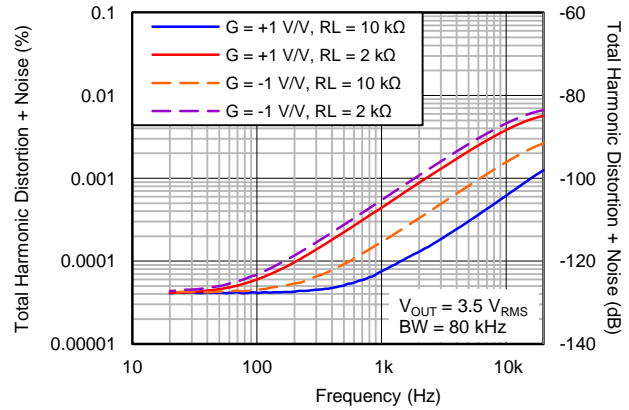


Figure 26. THD+N Ratio vs Frequency

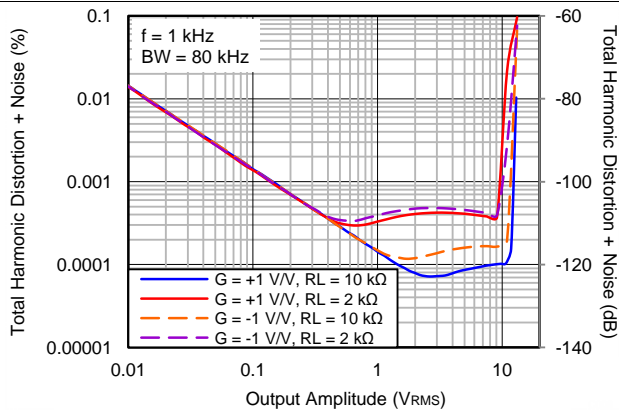


Figure 27. THD+N vs Output Amplitude

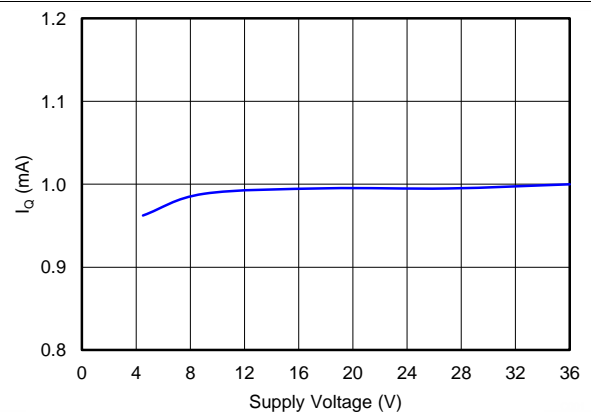


Figure 28. Quiescent Current vs Supply Voltage

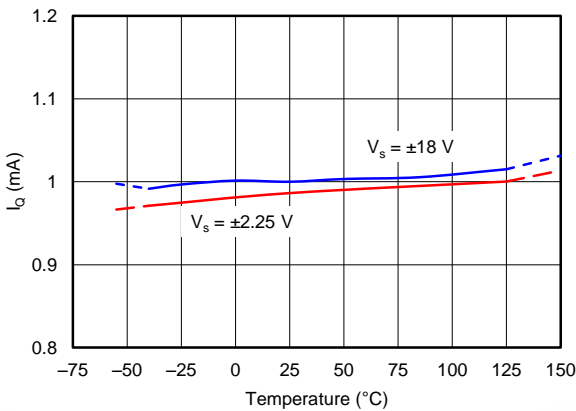


Figure 29. Quiescent Current vs Temperature

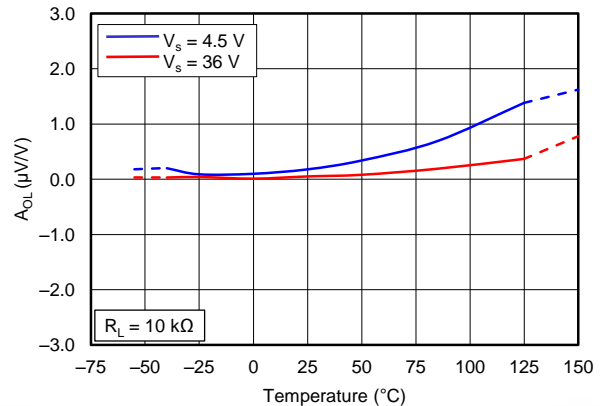


Figure 30. Open-Loop Gain vs Temperature

At $T_A = 25^\circ\text{C}$, $V_S = \pm 18\text{ V}$, $V_{CM} = V_S / 2$, $R_{LOAD} = 10\text{ k}\Omega$ connected to $V_S / 2$, and $C_L = 100\text{ pF}$, unless otherwise noted.

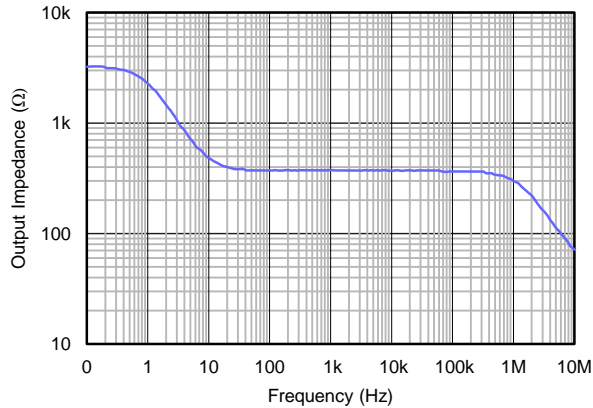


Figure 31. Open-Loop Output Impedance vs Frequency

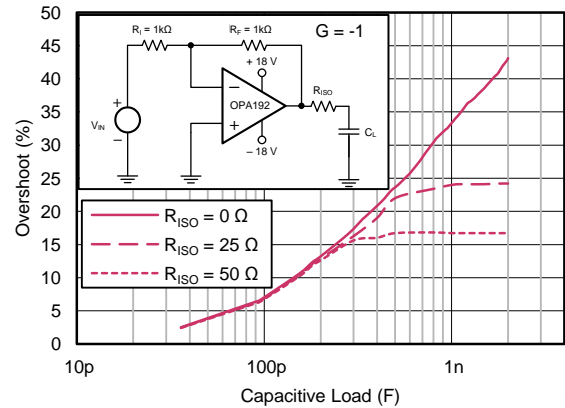


Figure 32. Small-Signal Overshoot vs Capacitive Load (100-mV Output Step)

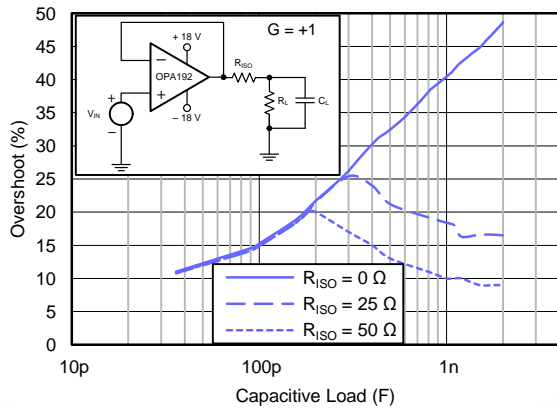


Figure 33. Small-Signal Overshoot vs Capacitive Load (100-mV Output Step)

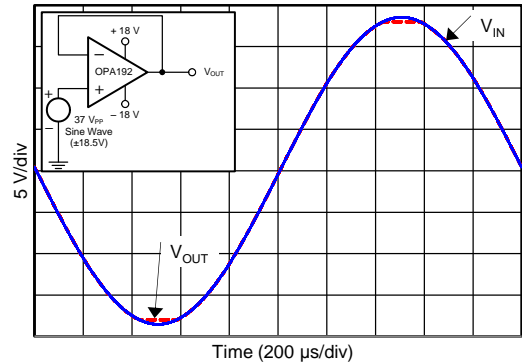


Figure 34. No Phase Reversal

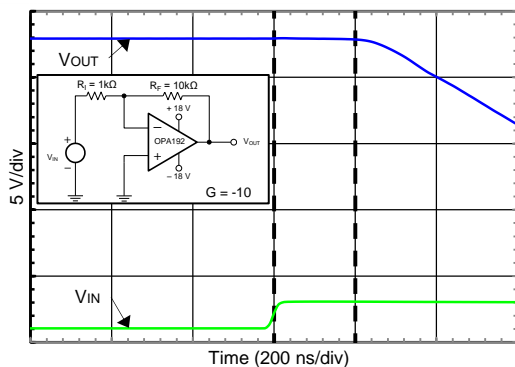


Figure 35. Positive Overload Recovery

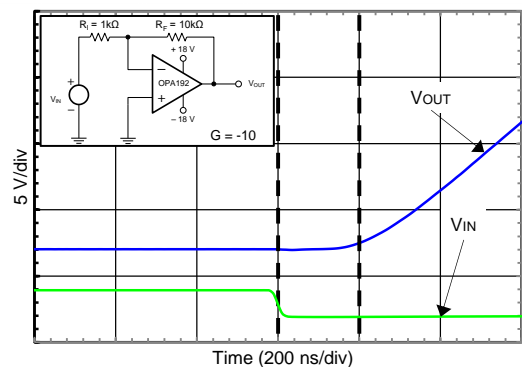


Figure 36. Negative Overload Recovery

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At $T_A = 25^\circ\text{C}$, $V_S = \pm 18\text{ V}$, $V_{CM} = V_S / 2$, $R_{LOAD} = 10\text{ k}\Omega$ connected to $V_S / 2$, and $C_L = 100\text{ pF}$, unless otherwise noted.

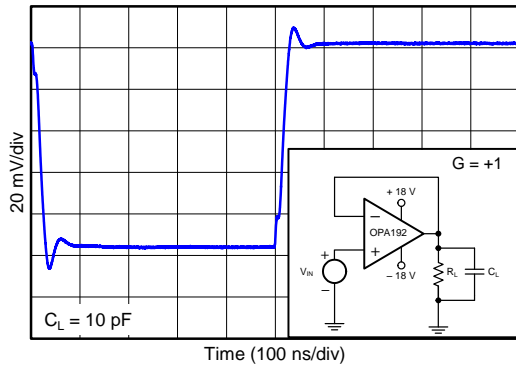


Figure 37. Small-Signal Step Response (100 mV)

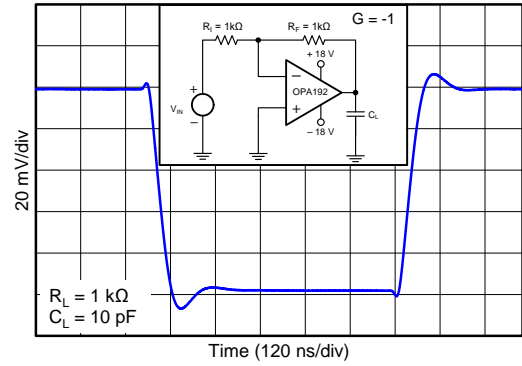


Figure 38. Small-Signal Step Response (100 mV)

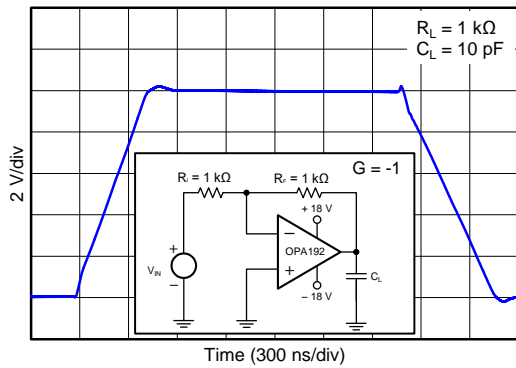


Figure 39. Large-Signal Step Response

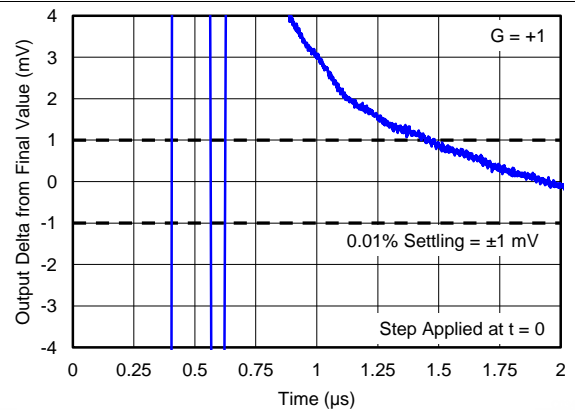


Figure 40. Settling Time (10-V Positive Step)

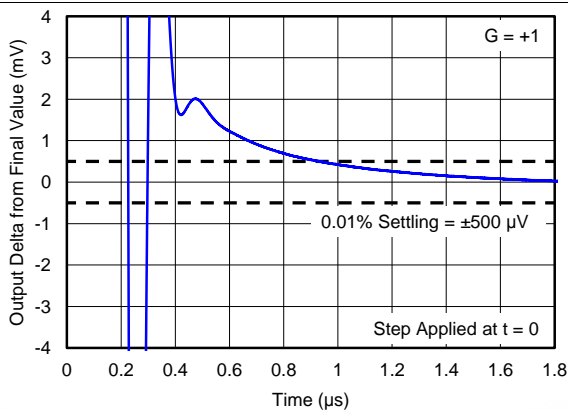


Figure 41. Settling Time (5-V Positive Step)

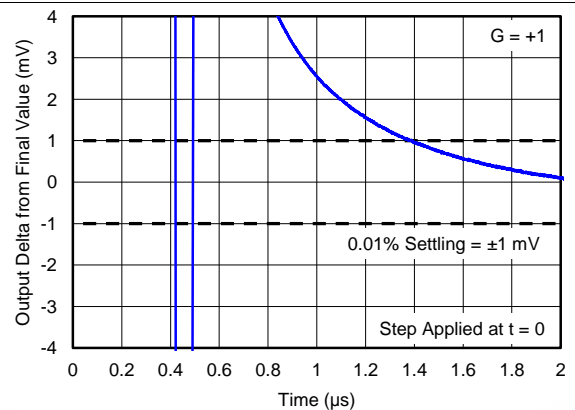


Figure 42. Settling Time (10-V Negative Step)

At $T_A = 25^\circ\text{C}$, $V_S = \pm 18\text{ V}$, $V_{CM} = V_S / 2$, $R_{LOAD} = 10\text{ k}\Omega$ connected to $V_S / 2$, and $C_L = 100\text{ pF}$, unless otherwise noted.

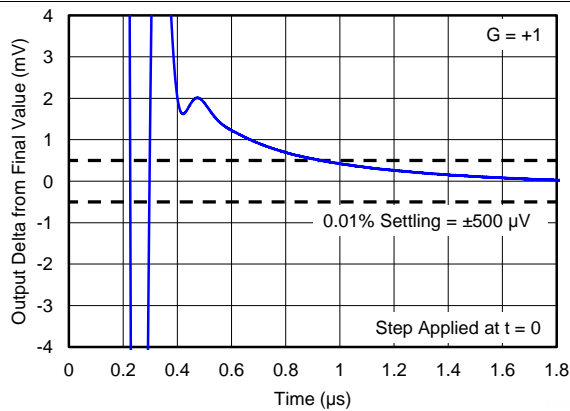


Figure 43. Settling Time (5-V Negative Step)

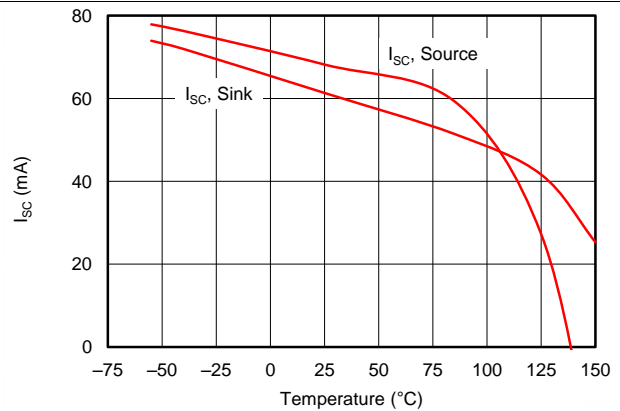


Figure 44. Short-Circuit Current vs Temperature

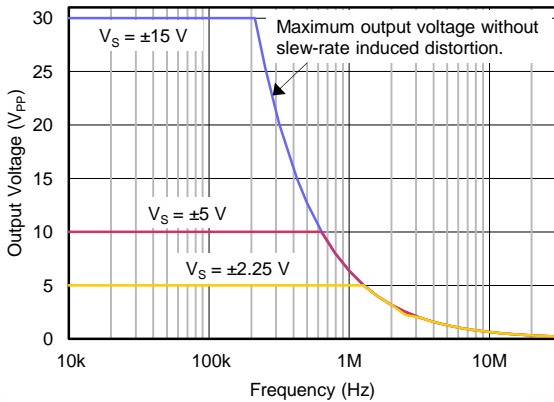


Figure 45. Maximum Output Voltage vs Frequency

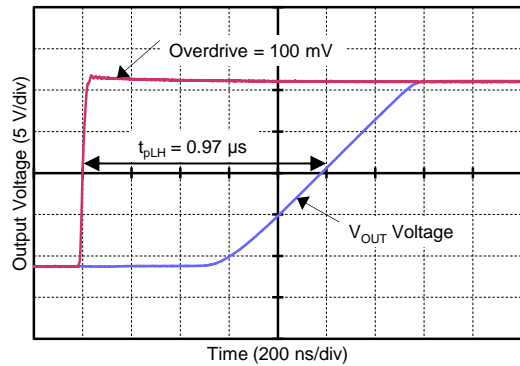


Figure 46. Propagation Delay Rising Edge

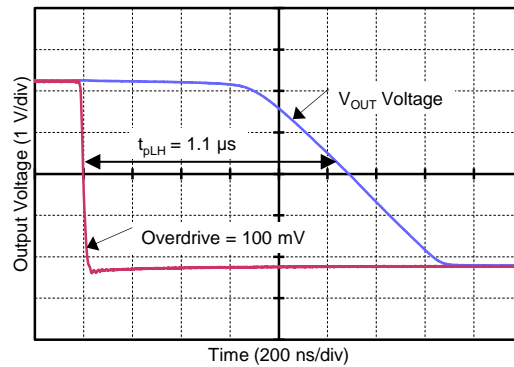


Figure 47. Propagation Delay Falling Edge

7 Parameter Measurement Information

7.1 Input Offset Voltage Drift

The OPAx192 family of operational amplifiers is manufactured using TI’s e-trim technology. Each amplifier input offset voltage and input offset drift is trimmed in production, thereby minimizing errors associated with input offset voltage and input offset voltage drift. The e-trim technology is a TI proprietary method of trimming internal device parameters during either wafer probing or final testing. When trimming input offset voltage drift the systematic or linear drift error on each device is trimmed to zero. This results in the remaining errors associated with input offset drift are minimal and are the result from only nonlinear error sources. Figure 48 illustrates this concept.

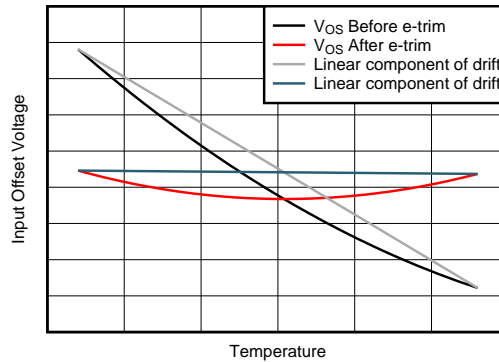


Figure 48. Input Offset Before and After Drift Trim

A common method of specifying input offset voltage drift is the *box method*. The box method estimates a maximum input offset drift by bounding the offset voltage versus temperature curve with a box and using the corners of this bounding box to determine the drift. The slope of the line connecting the diagonal corners of the box corresponds to the input offset voltage drift. Figure 49 illustrates the box method concept. The box method works particularly well when the input offset drift is dominated by the linear component input offset voltage drift, but because the OPA192 family uses TI’s e-trim technology to remove the linear component input offset voltage drift, the box method is not a particularly useful method of accurately performing an error analysis. Shown in Figure 49 are 30 typical units of OPAx192 with the box method superimposed for illustrative purposes. The boundaries of the box are determined by the specified temperature range along the x-axis and the maximum specified input offset voltage across that same temperature range along the y-axis. Using the box method predicts an input offset voltage drift of 0.9 $\mu\text{V}/^\circ\text{C}$. As shown in Figure 49, the slopes of the actual input offset voltage versus temperature are much less than that predicted by the box method. The box method predicts a pessimistic value for the maximum input offset voltage drift and is not recommended when performing an error analysis.

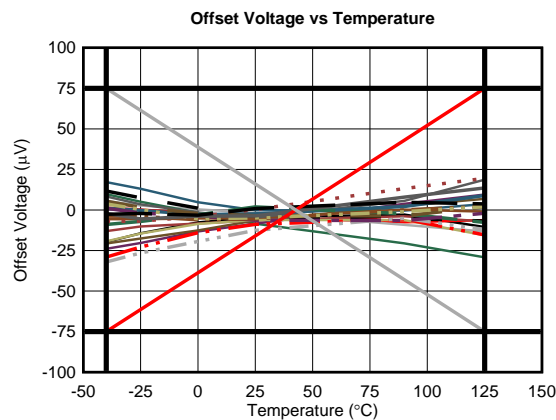
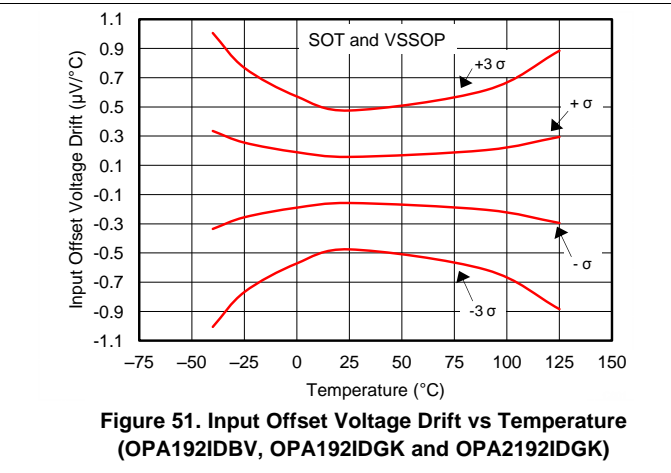
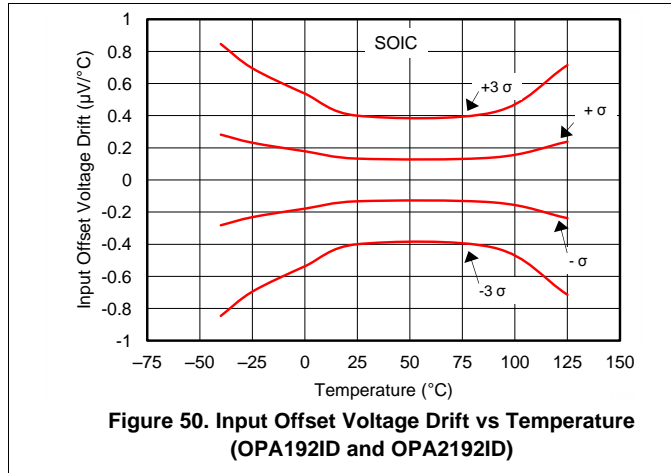


Figure 49. The Box Method

Input Offset Voltage Drift (continued)

Instead of the box method, a convenient way to illustrate input offset drift is to compute the slopes of the input offset voltage versus temperature curve. This is the same as computing the input offset drift at each point along the input offset voltage versus temperature curve. The results for the OPAx192 family are illustrated in [Figure 50](#) and [Figure 51](#).



As illustrated in [Figure 50](#), the input offset drift is typically less than $\pm 0.3 \mu\text{V}/^\circ\text{C}$ over the range from -40°C to $+125^\circ\text{C}$. When performing an error analysis over the full specified temperature range, use the typical and maximum values for input offset voltage drift as described in the *Electrical Characteristics* tables. If a reduced temperature range is applicable, use the information illustrated in [Figure 50](#) or [Figure 51](#) when performing an error analysis. To determine the change in input offset voltage, use [Equation 1](#):

$$\Delta V_{OS} = \Delta T \times dV_{OS}/dT$$

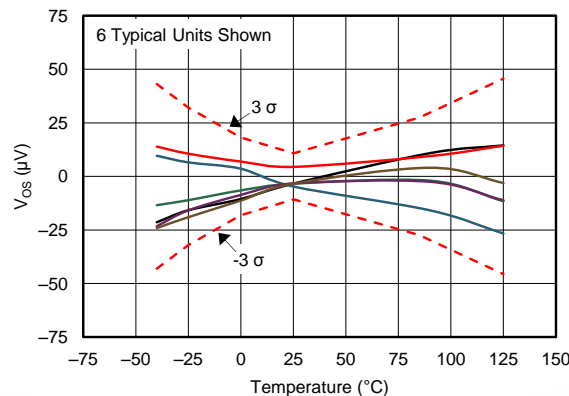
where

- ΔV_{OS} = Change in input offset voltage
- ΔT = Change in temperature
- dV_{OS}/dT = Input offset voltage drift (1)

For example, determine the amount of OPA192ID input offset voltage change over the temperature range of 25°C to 75°C for 1σ (68%) of the units. As shown in [Figure 50](#), the input offset drift is typically $0.15 \mu\text{V}/^\circ\text{C}$. This input offset drift results in a typical input offset voltage change of $(75^\circ\text{C} - 25^\circ\text{C}) \times 0.15 \mu\text{V}/^\circ\text{C} = 7.5 \mu\text{V}$.

For 3σ (99.7%) of the units, [Figure 50](#) shows a typical input offset drift of $0.4 \mu\text{V}/^\circ\text{C}$. This input offset drift results in a typical input offset voltage change of $(75^\circ\text{C} - 25^\circ\text{C}) \times 0.4 \mu\text{V}/^\circ\text{C} = 20 \mu\text{V}$.

[Figure 52](#) is illustrative of six typical units.



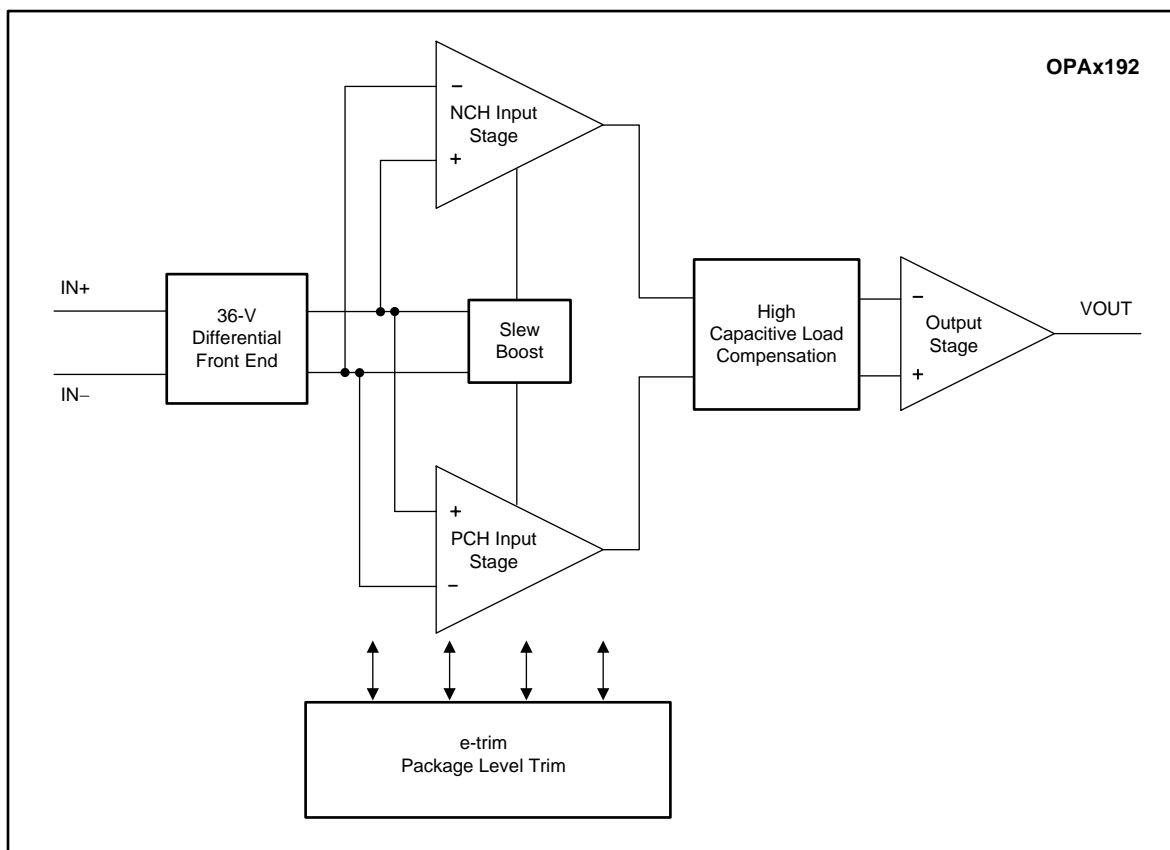
8 Detailed Description

8.1 Overview

The OPAx192 family of operational amplifiers use *e-trim*, a method of package-level trim for offset and offset temperature drift implemented during the final steps of manufacturing after the plastic molding process. This method minimizes the influence of inherent input transistor mismatch, as well as errors induced during package molding. The trim communication occurs on the output pin of the standard pinout, and after the trim points are set, further communication to the trim structure is permanently disabled. The [Functional Block Diagram](#) section shows the simplified diagram of the OPA192 with *e-trim*.

Unlike previous *e-trim* op amps, the OPAx192 uses a patented two-temperature trim architecture to achieve a very low offset voltage of 25 μV (max) and low voltage offset drift of 0.5 $\mu\text{V}/^\circ\text{C}$ (max) over the full specified temperature range. This level of precision performance at wide supply voltages makes these amplifiers useful for high-impedance industrial sensors, filters, and high-voltage data acquisition.

8.2 Functional Block Diagram



8.3 Feature Description

8.3.1 Input Protection Circuitry

The OPAx192 uses a unique input architecture to eliminate the need for input protection diodes but still provides robust input protection under transient conditions. Conventional input diode protection schemes shown in Figure 53 can be activated by fast transient step responses and can introduce signal distortion and settling time delays because of alternate current paths, as shown in Figure 54. For low-gain circuits, these fast-ramping input signals forward-bias back-to-back diodes, causing an increase in input current, and resulting in extended settling time, as shown in Figure 55.

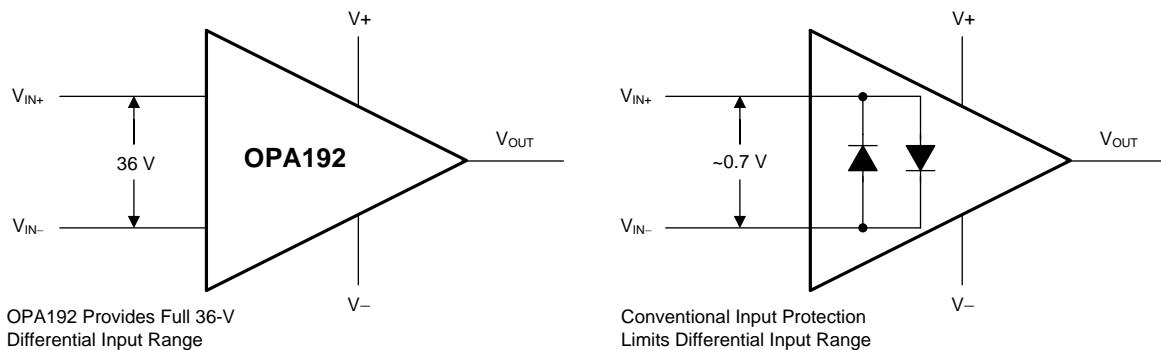


Figure 53. OPA192 Input Protection Does Not Limit Differential Input Capability

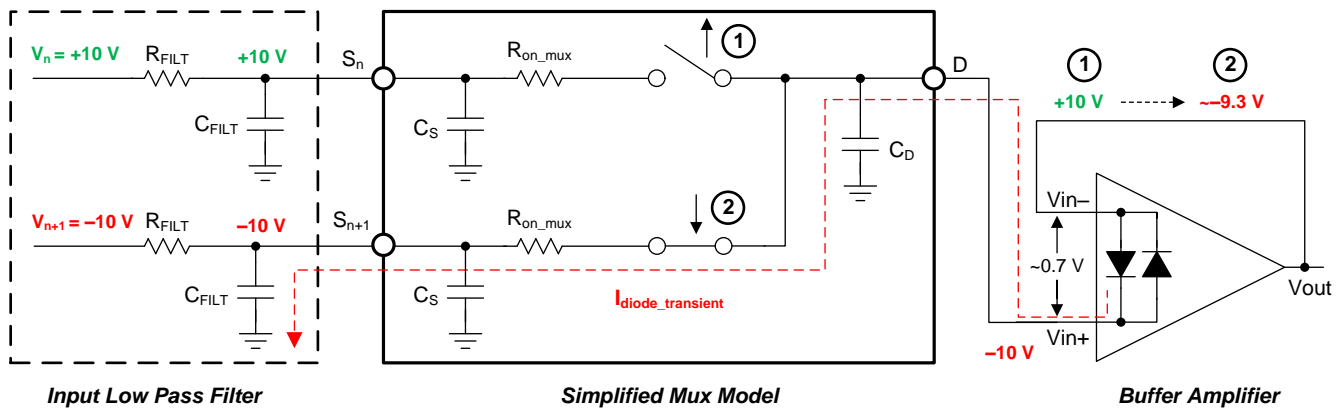


Figure 54. Back-to-Back Diodes Create Settling Issues

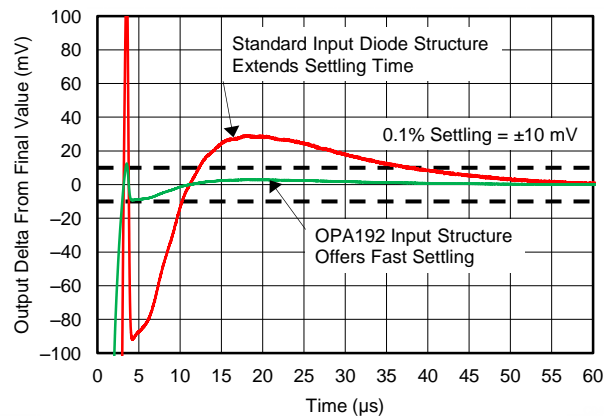


Figure 55. OPA192 Protection Circuit Maintains Fast-Settling Transient Response

Feature Description (continued)

The OPAx192 family of operational amplifiers provides a true high-impedance differential input capability for high-voltage applications. This patented input protection architecture does not introduce additional signal distortion or delayed settling time, making the device an optimal op amp for multichannel, high-switched, input applications. The OPA192 can tolerate a maximum differential swing (voltage between inverting and noninverting pins of the op amp) of up to 36 V, making the device suitable for use as a comparator or in applications with fast-ramping input signals such as multiplexed data-acquisition systems, as shown in [Figure 65](#).

8.3.2 EMI Rejection

The OPAx192 uses integrated electromagnetic interference (EMI) filtering to reduce the effects of EMI from sources such as wireless communications and densely-populated boards with a mix of analog signal chain and digital components. EMI immunity can be improved with circuit design techniques; the OPAx192 benefits from these design improvements. Texas Instruments has developed the ability to accurately measure and quantify the immunity of an operational amplifier over a broad frequency spectrum extending from 10 MHz to 6 GHz. [Figure 56](#) shows the results of this testing on the OPA192. [Table 2](#) shows the EMIRR IN+ values for the OPA192 at particular frequencies commonly encountered in real-world applications. Applications listed in [Table 2](#) may be centered on or operated near the particular frequency shown. Detailed information can also be found in the application report *EMI Rejection Ratio of Operational Amplifiers*, [SBOA128](#), available for download from [www.ti.com](#).

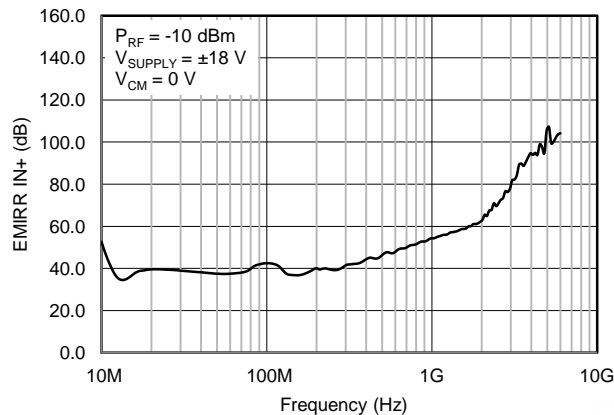


Figure 56. EMIRR Testing

Table 2. OPA192 EMIRR IN+ For Frequencies of Interest

FREQUENCY	APPLICATION OR ALLOCATION	EMIRR IN+
400 MHz	Mobile radio, mobile satellite, space operation, weather, radar, ultra-high frequency (UHF) applications	44.1 dB
900 MHz	Global system for mobile communications (GSM) applications, radio communication, navigation, GPS (to 1.6 GHz), GSM, aeronautical mobile, UHF applications	52.8 dB
1.8 GHz	GSM applications, mobile personal communications, broadband, satellite, L-band (1 GHz to 2 GHz)	61.0 dB
2.4 GHz	802.11b, 802.11g, 802.11n, Bluetooth®, mobile personal communications, industrial, scientific and medical (ISM) radio band, amateur radio and satellite, S-band (2 GHz to 4 GHz)	69.5 dB
3.6 GHz	Radiolocation, aero communication and navigation, satellite, mobile, S-band	88.7 dB
5.0 GHz	802.11a, 802.11n, aero communication and navigation, mobile communication, space and satellite operation, C-band (4 GHz to 8 GHz)	105.5 dB

8.3.3 Phase Reversal Protection

The OPAx192 family has internal phase-reversal protection. Many op amps exhibit a phase reversal when the input is driven beyond its linear common-mode range. This condition is most often encountered in noninverting circuits when the input is driven beyond the specified common-mode voltage range, causing the output to reverse into the opposite rail. The OPAx192 is a rail-to-rail input op amp; therefore, the common-mode range can extend up to the rails. Input signals beyond the rails do not cause phase reversal; instead, the output limits into the appropriate rail. This performance is shown in Figure 57.

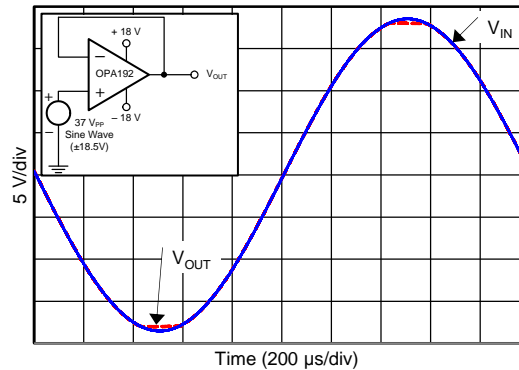


Figure 57. No Phase Reversal

8.3.4 Thermal Protection

The internal power dissipation of any amplifier causes its internal (junction) temperature to rise. This phenomenon is called *self heating*. The absolute maximum junction temperature of the OPAx192 is 150°C. Exceeding this temperature causes damage to the device. The OPAx192 has a thermal protection feature that prevents damage from self heating. The protection works by monitoring the temperature of the device and turning off the op amp output drive for temperatures above 140°C. Figure 58 shows an application example for the OPA192 that has significant self heating (159°C) because of its power dissipation (0.81 W). Thermal calculations indicate that for an ambient temperature of 65°C the device junction temperature must reach 187°C. The actual device, however, turns off the output drive to maintain a safe junction temperature. Figure 58 depicts how the circuit behaves during thermal protection. During normal operation, the device acts as a buffer so the output is 3 V. When self heating causes the device junction temperature to increase above 140°C, the thermal protection forces the output to a high-impedance state and the output is pulled to ground through resistor RL.

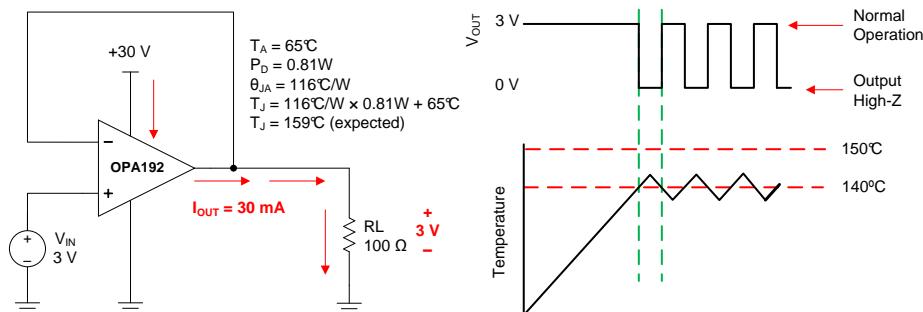


Figure 58. Thermal Protection

8.3.5 Capacitive Load and Stability

The OPAx192 features a patented output stage capable of driving large capacitive loads, and in a unity-gain configuration, directly drives up to 1 nF of pure capacitive load. Increasing the gain enhances the ability of the amplifier to drive greater capacitive loads; see Figure 59 and Figure 60. The particular op amp circuit configuration, layout, gain, and output loading are some of the factors to consider when establishing whether an amplifier will be stable in operation.

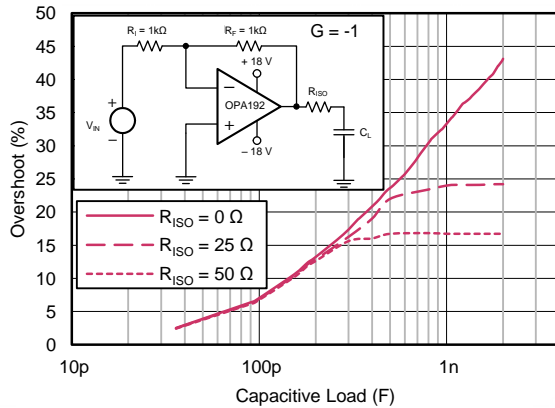


Figure 59. Small-Signal Overshoot vs Capacitive Load (100-mV Output Step)

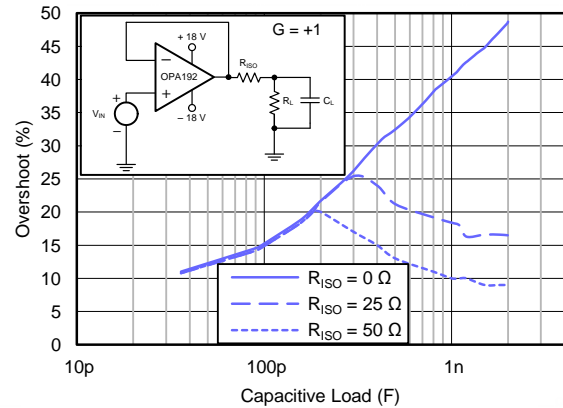


Figure 60. Small-Signal Overshoot vs Capacitive Load (100-mV Output Step)

For additional drive capability in unity-gain configurations, improve capacitive load drive by inserting a small (10 Ω to 20 Ω) resistor, R_{ISO} , in series with the output, as shown in Figure 61. This resistor significantly reduces ringing while maintaining dc performance for purely capacitive loads. However, if there is a resistive load in parallel with the capacitive load, a voltage divider is created, introducing a gain error at the output and slightly reducing the output swing. The error introduced is proportional to the ratio R_{ISO} / R_L , and is generally negligible at low output levels. A high capacitive load drive makes the OPA192 well suited for applications such as reference buffers, MOSFET gate drives, and cable-shield drives. The circuit shown in Figure 61 uses an isolation resistor, R_{ISO} , to stabilize the output of an op amp. R_{ISO} modifies the open-loop gain of the system for increased phase margin, and results using the OPA192 are summarized in Table 3. For additional information on techniques to optimize and design using this circuit, TI Precision Design TIDU032 details complete design goals, simulation, and test results.

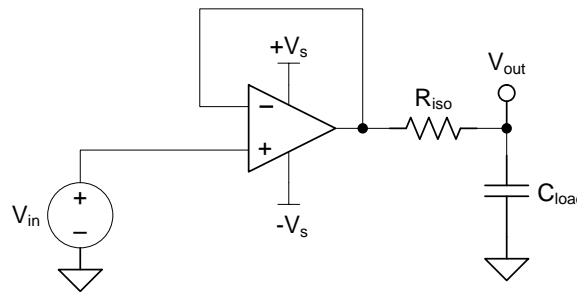


Figure 61. Extending Capacitive Load Drive with the OPA192

Table 3. OPA192 Capacitive Load Drive Solution Using Isolation Resistor Comparison of Calculated and Measured Results

PARAMETER	VALUE										
	100 pF		1000 pF		0.01 μF		0.1 μF		1 μF		
Capacitive Load	100 pF		1000 pF		0.01 μF		0.1 μF		1 μF		
Phase Margin	45°	60°	45°	60°	45°	60°	45°	60°	45°	60°	
R_{ISO} (Ω)	47.0	360.0	24.0	100.0	20.0	51.0	6.2	15.8	2.0	4.7	
Measured Overshoot (%)	23.2	8.6	10.4	22.5	9.0	22.1	8.7	23.1	8.6	21.0	8.6
Calculated PM	45.1°	58.1°	45.8°	59.7°	46.1°	60.1°	45.2°	60.2°	47.2°	60.2°	



For step-by-step design procedure, circuit schematics, bill of materials, printed circuit board (PCB) files, simulation results, and test results, refer to TI Precision Design TIDU032, [Capacitive Load Drive Solution using an Isolation Resistor](#).

8.3.6 Common-Mode Voltage Range

The OPAx192 is a 36-V, true rail-to-rail input operational amplifier with an input common-mode range that extends 100 mV beyond either supply rail. This wide range is achieved with paralleled complementary N-channel and P-channel differential input pairs, as shown in Figure 62. The N-channel pair is active for input voltages close to the positive rail, typically $(V+) - 3\text{ V}$ to 100 mV above the positive supply. The P-channel pair is active for inputs from 100 mV below the negative supply to approximately $(V+) - 1.5\text{ V}$. There is a small transition region, typically $(V+) - 3\text{ V}$ to $(V+) - 1.5\text{ V}$ in which both input pairs are on. This transition region can vary modestly with process variation, and within this region PSRR, CMRR, offset voltage, offset drift, noise and THD performance may be degraded compared to operation outside this region.

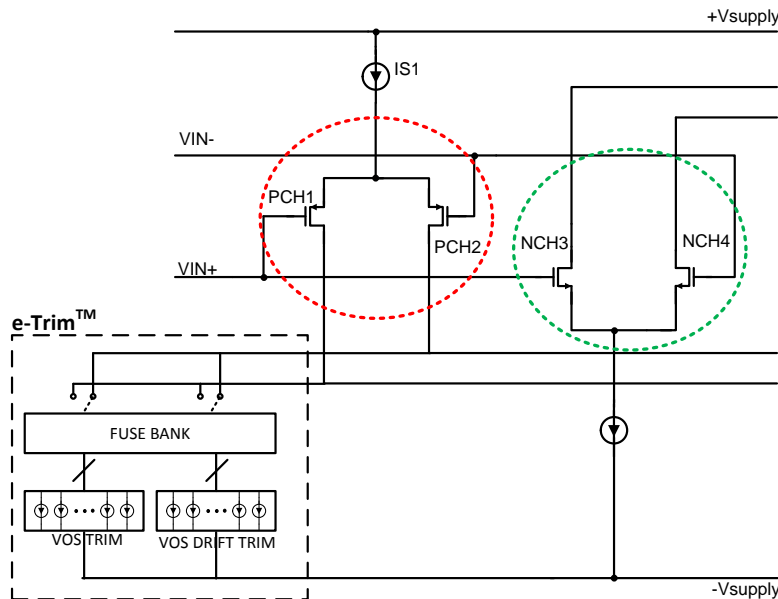


Figure 62. Rail-to-Rail Input Stage

To achieve the best performance for two-stage rail-to-rail input amplifiers, avoid the transition region when possible. The OPAx192 uses a precision trim for both the N-channel and P-channel regions. This technique enables significantly lower levels of offset than previous-generation devices, causing variance in the transition region of the input stages to appear exaggerated relative to offset over the full common-mode range, as shown in Figure 63.

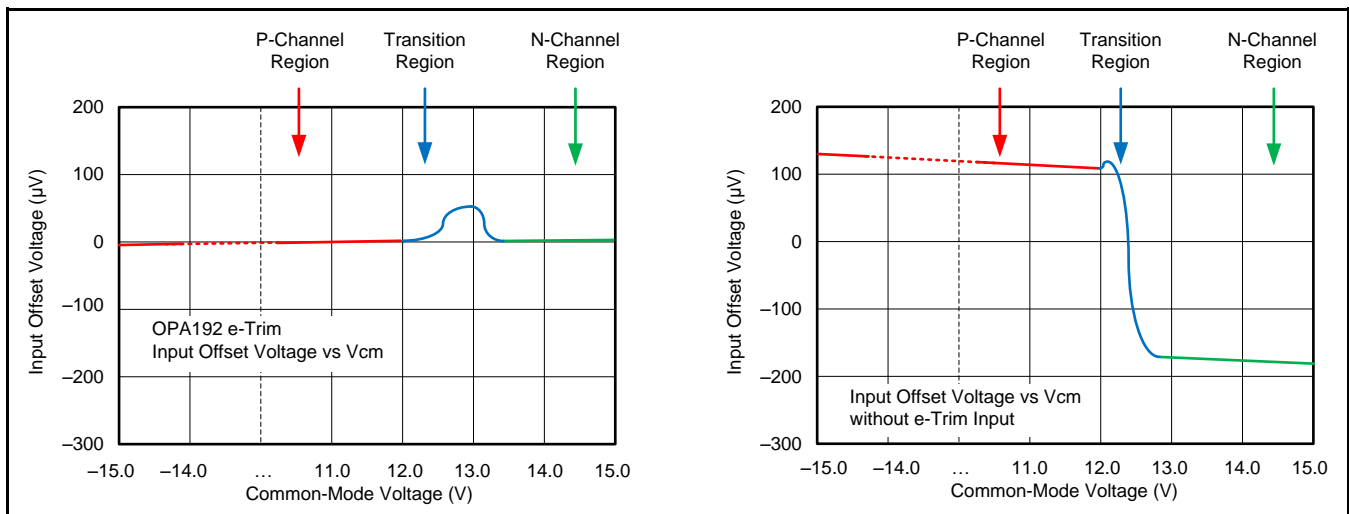


Figure 63. Common-Mode Transition vs Standard Rail-to-Rail Amplifiers

8.3.7 Electrical Overstress

Designers often ask questions about the capability of an operational amplifier to withstand electrical overstress (EOS). These questions tend to focus on the device inputs, but may involve the supply voltage pins or even the output pin. Each of these different pin functions have electrical stress limits determined by the voltage breakdown characteristics of the particular semiconductor fabrication process and specific circuits connected to the pin. Additionally, internal electrostatic discharge (ESD) protection is built into these circuits to protect them from accidental ESD events both before and during product assembly.

Having a good understanding of this basic ESD circuitry and its relevance to an electrical overstress event is helpful. See [Figure 64](#) for an illustration of the ESD circuits contained in the OPAx192 (indicated by the dashed line area). The ESD protection circuitry involves several current-steering diodes connected from the input and output pins and routed back to the internal power-supply lines, where the diodes meet at an absorption device or the power-supply ESD cell, internal to the operational amplifier. This protection circuitry is intended to remain inactive during normal circuit operation.

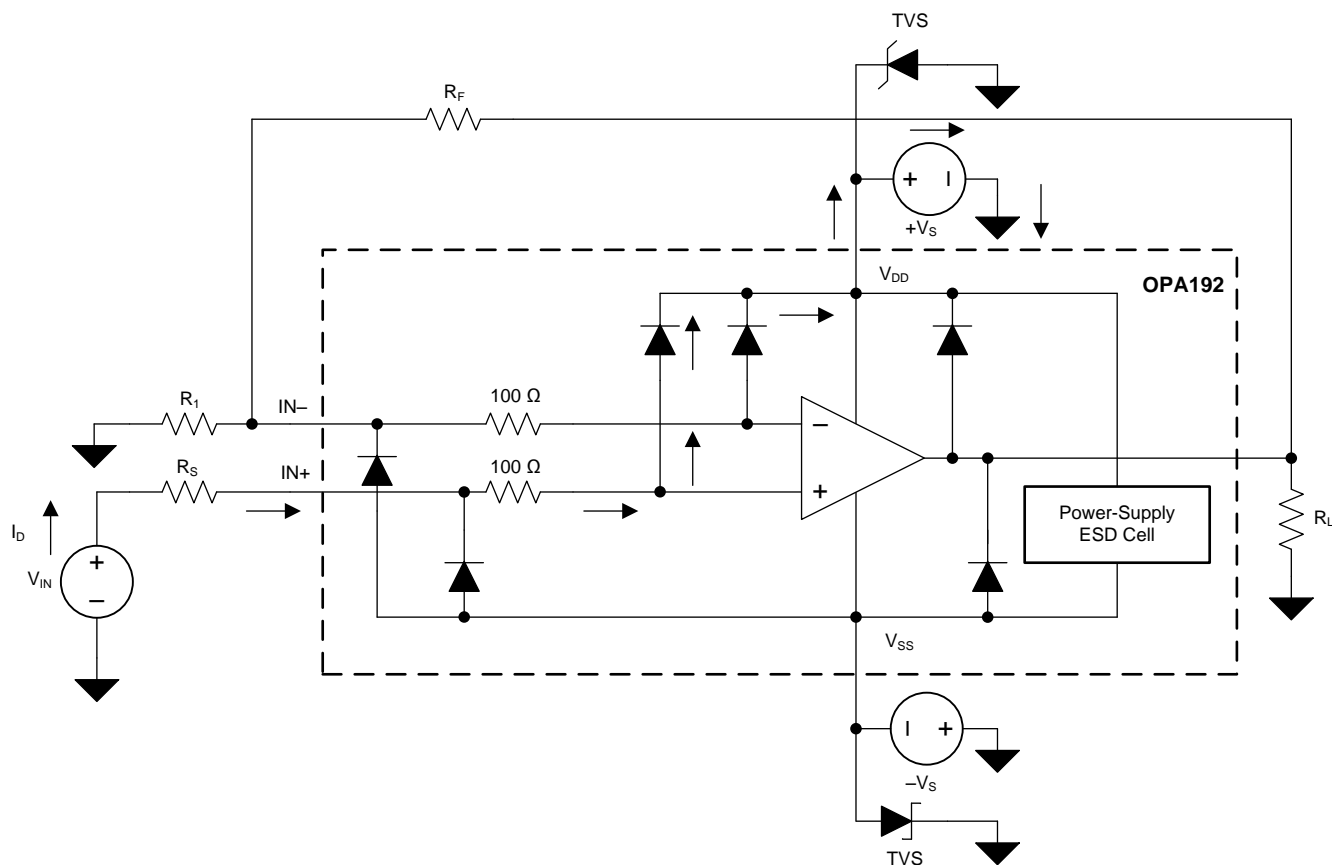


Figure 64. Equivalent Internal ESD Circuitry Relative to a Typical Circuit Application

An ESD event is very short in duration and very high voltage (for example, 1 kV, 100 ns), whereas an EOS event is long duration and lower voltage (for example, 50 V, 100 ms). The ESD diodes are designed for out-of-circuit ESD protection (that is, during assembly, test, and storage of the device before being soldered to the PCB). During an ESD event, the ESD signal is passed through the ESD steering diodes to an absorption circuit (labeled ESD power-supply circuit). The ESD absorption circuit clamps the supplies to a safe level.

Although this behavior is necessary for out-of-circuit protection, excessive current and damage is caused if activated in-circuit. A transient voltage suppressors (TVS) can be used to prevent against damage caused by turning on the ESD absorption circuit during an in-circuit ESD event. Using the appropriate current limiting resistors and TVS diodes allows for the use of device ESD diodes to protect against EOS events.

8.3.8 Overload Recovery

Overload recovery is defined as the time required for the op amp output to recover from a saturated state to a linear state. The output devices of the op amp enter a saturation region when the output voltage exceeds the rated operating voltage, either due to the high input voltage or the high gain. After the device enters the saturation region, the charge carriers in the output devices require time to return back to the linear state. After the charge carriers return back to the linear state, the device begins to slew at the specified slew rate. Thus, the propagation delay in case of an overload condition is the sum of the overload recovery time and the slew time. The overload recovery time for the OPAx192 is approximately 200 ns.

8.4 Device Functional Modes

The OPAx192 has a single functional mode and is operational when the power-supply voltage is greater than 4.5 V (± 2.25 V). The maximum power supply voltage for the OPAx192 is 36 V (± 18 V).

9 Application and Implementation

NOTE

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

9.1 Application Information

The OPAx192 family offers outstanding dc precision and ac performance. These devices operate up to 36-V supply rails and offer true rail-to-rail input/output, ultralow offset voltage and offset voltage drift, as well as 10-MHz bandwidth and high capacitive load drive. These features make the OPAx192 a robust, high-performance operational amplifier for high-voltage industrial applications.

9.2 Typical Applications

9.2.1 16-Bit Precision Multiplexed Data-Acquisition System

Figure 65 shows a 16-bit, differential, 4-channel, multiplexed data-acquisition system. This example is typical in industrial applications that require low distortion and a high-voltage differential input. The circuit uses the ADS8864, a 16-bit, 400-kSPS successive-approximation-resistor (SAR) analog-to-digital converter (ADC), along with a precision, high-voltage, signal-conditioning front end, and a 4-channel differential multiplexer (mux). This TI Precision Design details the process for optimizing the precision, high-voltage, front-end drive circuit using the OPA192 and OPA140 to achieve excellent dynamic performance and linearity with the ADS8864.

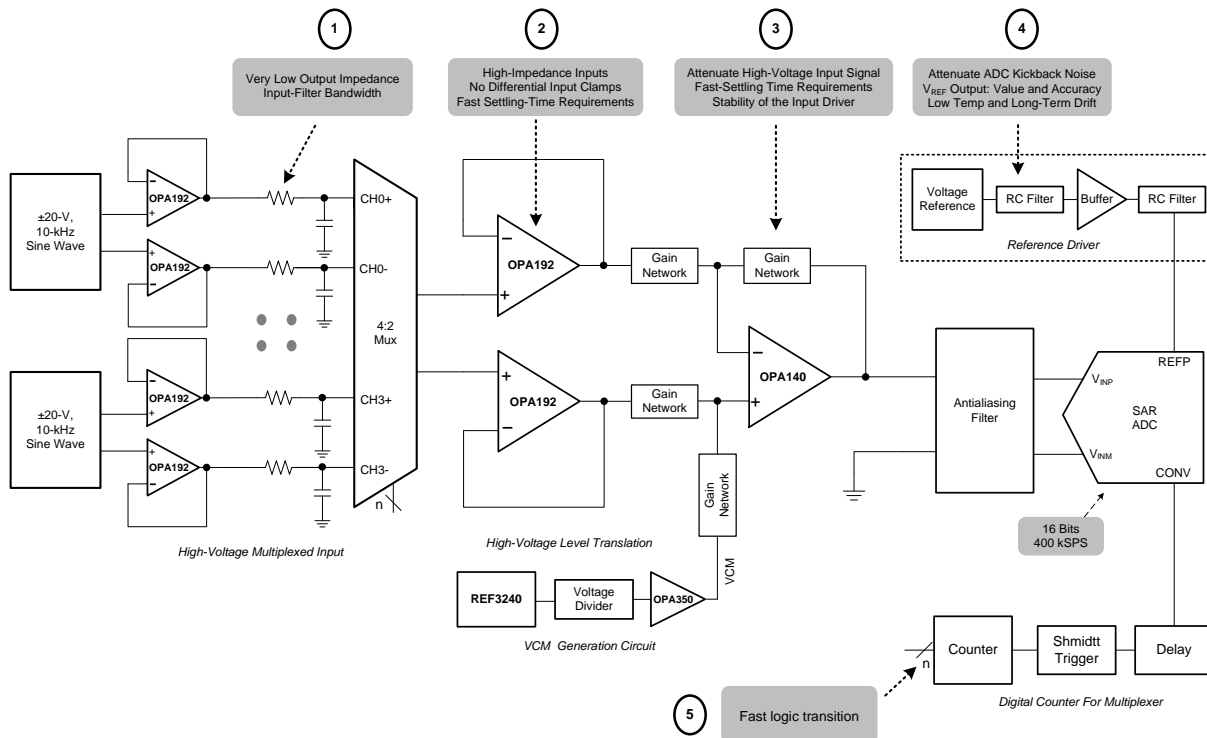


Figure 65. OPA192 in 16-Bit, 400-kSPS, 4-Channel, Multiplexed Data Acquisition System for High-Voltage Inputs with Lowest Distortion

9.2.1.1 Design Requirements

The primary objective is to design a ± 20 V, differential 4-channel multiplexed data acquisition system with lowest distortion using the 16-bit ADS8864 at a throughput of 400 kSPS for a 10 kHz full-scale pure sine-wave input. The design requirements for this block design are:

Typical Applications (continued)

- System Supply Voltage: ± 15 V
- ADC Supply Voltage: 3.3 V
- ADC Sampling Rate: 400 kSPS
- ADC Reference Voltage (REFP): 4.096 V
- System Input Signal: A high-voltage differential input signal with a peak amplitude of 10 V and frequency (f_{IN}) of 10 kHz are applied to each differential input of the mux.

9.2.1.2 Detailed Design Procedure

The purpose of this precision design is to design an optimal high voltage multiplexed data acquisition system for highest system linearity and fast settling. The overall system block diagram is shown in [Figure 65](#). The circuit is a multichannel data acquisition signal chain consisting of an input low-pass filter, multiplexer (mux), mux output buffer, attenuating SAR ADC driver, digital counter for mux and the reference driver. The architecture allows fast sampling of multiple channels using a single ADC, providing a low-cost solution. The two primary design considerations to maximize the performance of a precision multiplexed data acquisition system are the mux input analog front-end and the high-voltage level translation SAR ADC driver design. However, carefully design each analog circuit block based on the ADC performance specifications in order to achieve the fastest settling at 16-bit resolution and lowest distortion system. The diagram includes the most important specifications for each individual analog block.

This design systematically approaches each analog circuit block to achieve a 16-bit settling for a fullscale input stage voltage and linearity for a 10-kHz sinusoidal input signal at each input channel. The first step in the design is to understand the requirement for extremely low impedance input-filter design for the mux. This understanding helps in the decision of an appropriate input filter and selection of a mux to meet the system settling requirements. The next important step is the design of the attenuating analog front end (AFE) used to level translate the high-voltage input signal to a low-voltage ADC input while maintaining the amplifier stability. The next step is to design a digital interface to switch the mux input channels with minimum delay. The final design challenge is to design a high-precision, reference-driver circuit that provides the required REFP reference voltage with low offset, drift, and noise contributions.

9.2.1.3 Application Curve

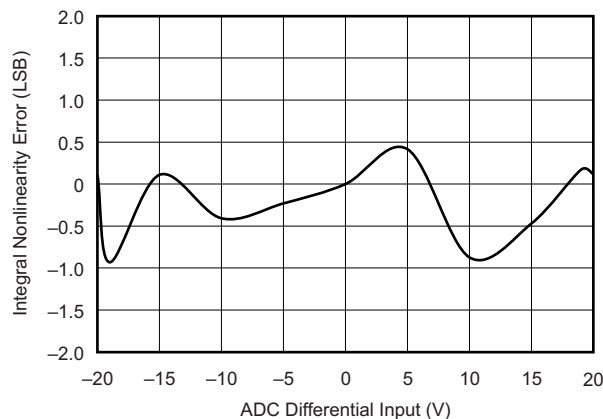


Figure 66. ADC 16-Bit Linearity Error for the Multiplexed Data Acquisition Block



For step-by-step design procedure, circuit schematics, bill of materials, PCB files, simulation results, and test results, refer to [TI Precision Design TIDU181, 16-bit, 400-kSPS, 4-Channel, Multiplexed Data Acquisition System for High Voltage Inputs with Lowest Distortion.](#)

9.2.2 Slew Rate Limit for Input Protection

In control systems for valves or motors, abrupt changes in voltages or currents can cause mechanical damages. By controlling the slew rate of the command voltages into the drive circuits, the load voltages ramps up and down at a safe rate. For symmetrical slew-rate applications (positive slew rate equals negative slew rate), one additional op amp provides slew-rate control for a given analog gain stage. The unique input protection and high output current and slew rate of the OPAx192 make the device an optimal amplifier to achieve slew rate control for both dual- and single-supply systems. [Figure 67](#) shows the OPA192 in a slew-rate limit design.

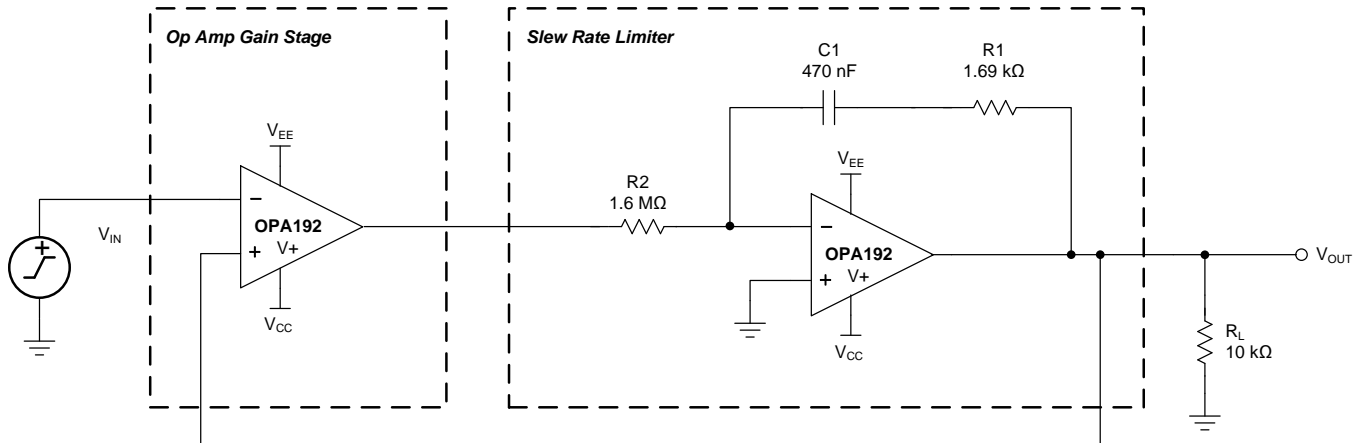


Figure 67. Slew Rate Limiter Uses One Op Amp



For step-by-step design procedure, circuit schematics, bill of materials, PCB files, simulation results, and test results, refer to [TI Precision Design TIDU026, Slew Rate Limiter Uses One Op Amp](#).

9.2.3 Precision Reference Buffer

The OPAx192 features high output current drive capability and low input offset voltage, making the device an excellent reference buffer to provide an accurate buffered output with ample drive current for transients. For the 10- μ F ceramic capacitor shown in [Figure 68](#), R_{ISO} , a 37.4- Ω isolation resistor, provides separation of two feedback paths for optimal stability. Feedback path number one is through R_F and is directly at the output, V_{OUT} . Feedback path number two is through R_{Fx} and C_F and is connected at the output of the op amp. The optimized stability components shown for the 10- μ F load give a closed-loop signal bandwidth at V_{OUT} of 4 kHz, while still providing a loop gain phase margin of 89°. Any other load capacitances require recalculation of the stability components: R_F , R_{Fx} , C_F , and R_{ISO} .

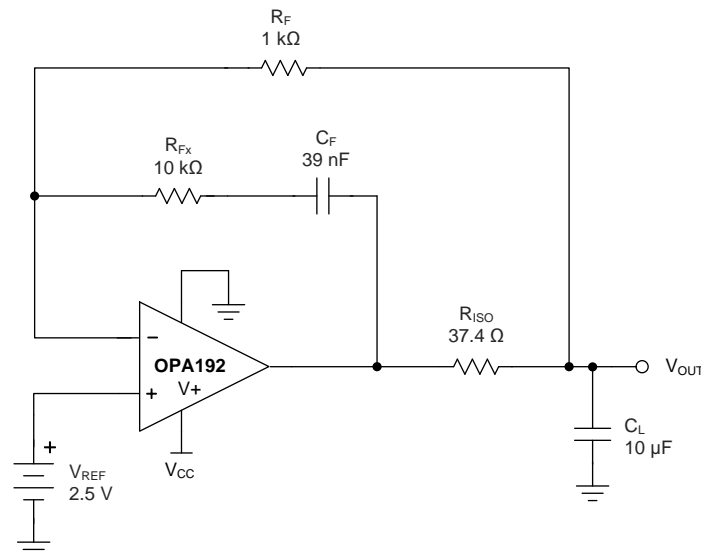


Figure 68. Precision Reference Buffer

10 Power-Supply Recommendations

The OPAx192 is specified for operation from 4.5 V to 36 V (± 2.25 V to ± 18 V); many specifications apply from -40°C to $+125^{\circ}\text{C}$. Parameters that can exhibit significant variance with regard to operating voltage or temperature are presented in the [Typical Characteristics](#).

CAUTION

Supply voltages larger than 40 V can permanently damage the device; see the [Absolute Maximum Ratings](#).

Place 0.1- μF bypass capacitors close to the power-supply pins to reduce errors coupling in from noisy or high-impedance power supplies. For more detailed information on bypass capacitor placement, refer to the [Layout](#) section.

11 Layout

11.1 Layout Guidelines

For best operational performance of the device, use good PCB layout practices, including:

- Noise can propagate into analog circuitry through the power pins of the circuit as a whole and op amp itself. Bypass capacitors are used to reduce the coupled noise by providing low-impedance power sources local to the analog circuitry.
 - Connect low-ESR, 0.1- μF ceramic bypass capacitors between each supply pin and ground, placed as close to the device as possible. A single bypass capacitor from V+ to ground is applicable for single-supply applications.
- Separate grounding for analog and digital portions of circuitry is one of the simplest and most-effective methods of noise suppression. One or more layers on multilayer PCBs are usually devoted to ground planes. A ground plane helps distribute heat and reduces EMI noise pickup. Make sure to physically separate digital and analog grounds paying attention to the flow of the ground current. For more detailed information refer to *Circuit Board Layout Techniques*, [SLOA089](#).
- In order to reduce parasitic coupling, run the input traces as far away from the supply or output traces as possible. If these traces cannot be kept separate, crossing the sensitive trace perpendicular is much better as opposed to in parallel with the noisy trace.
- Place the external components as close to the device as possible. As shown in [Figure 69](#), keeping RF and RG close to the inverting input minimizes parasitic capacitance.
- Keep the length of input traces as short as possible. Always remember that the input traces are the most sensitive part of the circuit.
- Consider a driven, low-impedance guard ring around the critical traces. A guard ring can significantly reduce leakage currents from nearby traces that are at different potentials.
- Cleaning the PCB following board assembly is recommended for best performance.
- Any precision integrated circuit may experience performance shifts due to moisture ingress into the plastic package. Following any aqueous PCB cleaning process, baking the PCB assembly is recommended to remove moisture introduced into the device packaging during the cleaning process. A low temperature, post cleaning bake at 85°C for 30 minutes is sufficient for most circumstances.

11.2 Layout Example

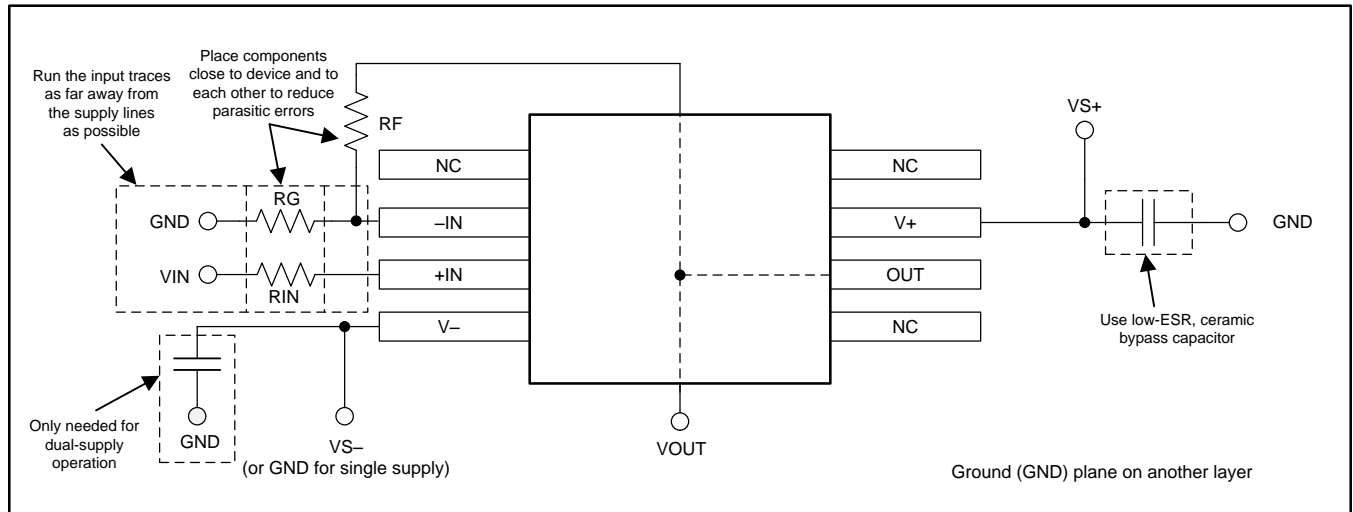
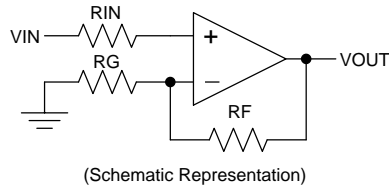


Figure 69. Operational Amplifier Board Layout for Noninverting Configuration

12 Device and Documentation Support

12.1 Device Support

12.1.1 Development Support

12.1.1.1 TINA-TI™ (Free Software Download)

TINA™ is a simple, powerful, and easy-to-use circuit simulation program based on a SPICE engine. TINA-TI is a free, fully-functional version of the TINA software, preloaded with a library of macro models in addition to a range of both passive and active models. TINA-TI provides all the conventional dc, transient, and frequency domain analysis of SPICE, as well as additional design capabilities.

Available as a [free download](#) from the Analog eLab Design Center, TINA-TI offers extensive post-processing capability that allows users to format results in a variety of ways. Virtual instruments offer the ability to select input waveforms and probe circuit nodes, voltages, and waveforms, creating a dynamic quick-start tool.

NOTE

These files require that either the TINA software (from DesignSoft™) or TINA-TI software be installed. Download the free TINA-TI software from the [TINA-TI folder](#).

12.1.1.2 TI Precision Designs

The OPA192 is featured in several TI Precision Designs, available online at <http://www.ti.com/ww/en/analog/precision-designs/>. TI Precision Designs are analog solutions created by TI's precision analog applications experts and offer the theory of operation, component selection, simulation, complete PCB schematic and layout, bill of materials, and measured performance of many useful circuits.

12.2 Documentation Support

12.2.1 Related Documentation

Circuit Board Layout Techniques, [SLOA089](#).

Op Amps for Everyone, [SLOD006](#).

12.3 Related Links

[Table 4](#) lists quick access links. Categories include technical documents, support and community resources, tools and software, and quick access to sample or buy.

Table 4. Related Links

PARTS	PRODUCT FOLDER	SAMPLE & BUY	TECHNICAL DOCUMENTS	TOOLS & SOFTWARE	SUPPORT & COMMUNITY
OPA192	Click here	Click here	Click here	Click here	Click here
OPA2192	Click here	Click here	Click here	Click here	Click here
OPA4192	Click here	Click here	Click here	Click here	Click here

12.4 Trademarks

e-trim is a trademark of Texas Instruments.

TINA-TI is a trademark of Texas Instruments, Inc and DesignSoft, Inc.

Bluetooth is a registered trademark of Bluetooth SIG, Inc.

TINA, DesignSoft are trademarks of DesignSoft, Inc.

All other trademarks are the property of their respective owners.

12.5 Electrostatic Discharge Caution



This integrated circuit can be damaged by ESD. Texas Instruments recommends that all integrated circuits be handled with appropriate precautions. Failure to observe proper handling and installation procedures can cause damage.

ESD damage can range from subtle performance degradation to complete device failure. Precision integrated circuits may be more susceptible to damage because very small parametric changes could cause the device not to meet its published specifications.

12.6 Glossary

[SLYZ022](#) — *TI Glossary*.

This glossary lists and explains terms, acronyms, and definitions.

13 Mechanical, Packaging, and Orderable Information

The following pages include mechanical packaging and orderable information. This information is the most current data available for the designated devices. This data is subject to change without notice and revision of this document. For browser-based versions of this data sheet, refer to the left-hand navigation.

PACKAGING INFORMATION

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
OPA192ID	PREVIEW	SOIC	D	8	75	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	OPA192	
OPA192IDBVR	ACTIVE	SOT-23	DBV	5	3000	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	OUYS	Samples
OPA192IDBVT	ACTIVE	SOT-23	DBV	5	250	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	OUYS	Samples
OPA192IDGKR	ACTIVE	VSSOP	DGK	8	2500	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	OUXS	Samples
OPA192IDGKT	ACTIVE	VSSOP	DGK	8	250	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	OUXS	Samples
OPA192IDR	PREVIEW	SOIC	D	8	2500	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	OPA192	
OPA2192ID	ACTIVE	SOIC	D	8	75	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	2192	Samples
OPA2192IDGK	PREVIEW	VSSOP	DGK	8	80	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	OVLM	
OPA2192IDGKR	PREVIEW	VSSOP	DGK	8	2500	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	OVLM	
OPA2192IDR	ACTIVE	SOIC	D	8	2500	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	2192	Samples

(1) The marketing status values are defined as follows:

ACTIVE: Product device recommended for new designs.

LIFEBUY: TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

NRND: Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

PREVIEW: Device has been announced but is not in production. Samples may or may not be available.

OBSELETE: TI has discontinued the production of the device.

(2) Eco Plan - The planned eco-friendly classification: Pb-Free (RoHS), Pb-Free (RoHS Exempt), or Green (RoHS & no Sb/Br) - please check <http://www.ti.com/productcontent> for the latest availability information and additional product content details.

TBD: The Pb-Free/Green conversion plan has not been defined.

Pb-Free (RoHS): TI's terms "Lead-Free" or "Pb-Free" mean semiconductor products that are compatible with the current RoHS requirements for all 6 substances, including the requirement that lead not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, TI Pb-Free products are suitable for use in specified lead-free processes.

Pb-Free (RoHS Exempt): This component has a RoHS exemption for either 1) lead-based flip-chip solder bumps used between the die and package, or 2) lead-based die adhesive used between the die and leadframe. The component is otherwise considered Pb-Free (RoHS compatible) as defined above.

Green (RoHS & no Sb/Br): TI defines "Green" to mean Pb-Free (RoHS compatible), and free of Bromine (Br) and Antimony (Sb) based flame retardants (Br or Sb do not exceed 0.1% by weight in homogeneous material)

- (3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.
- (4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.
- (5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.
- (6) Lead/Ball Finish - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead/Ball Finish values may wrap to two lines if the finish value exceeds the maximum column width.

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TAPE AND REEL INFORMATION

QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE


*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
OPA192IDBVR	SOT-23	DBV	5	3000	180.0	8.4	3.23	3.17	1.37	4.0	8.0	Q3
OPA192IDBVT	SOT-23	DBV	5	250	180.0	8.4	3.23	3.17	1.37	4.0	8.0	Q3
OPA192IDGKR	VSSOP	DGK	8	2500	330.0	12.4	5.3	3.4	1.4	8.0	12.0	Q1
OPA192IDGKT	VSSOP	DGK	8	250	177.8	12.4	5.3	3.4	1.4	8.0	12.0	Q1

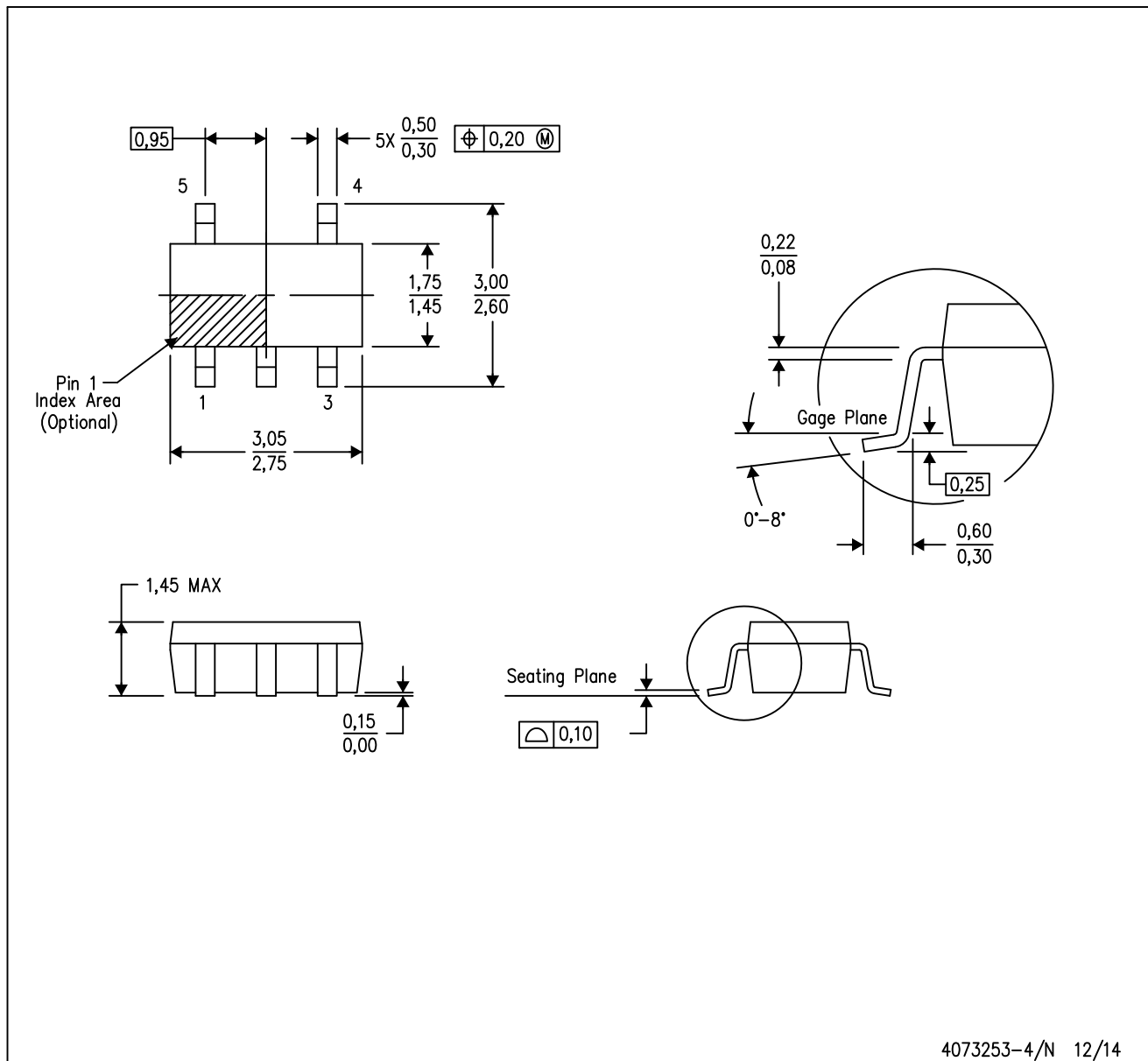
TAPE AND REEL BOX DIMENSIONS


*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
OPA192IDBVR	SOT-23	DBV	5	3000	223.0	270.0	35.0
OPA192IDBVT	SOT-23	DBV	5	250	223.0	270.0	35.0
OPA192IDGKR	VSSOP	DGK	8	2500	358.0	335.0	35.0
OPA192IDGKT	VSSOP	DGK	8	250	223.0	270.0	35.0

DBV (R-PDSO-G5)

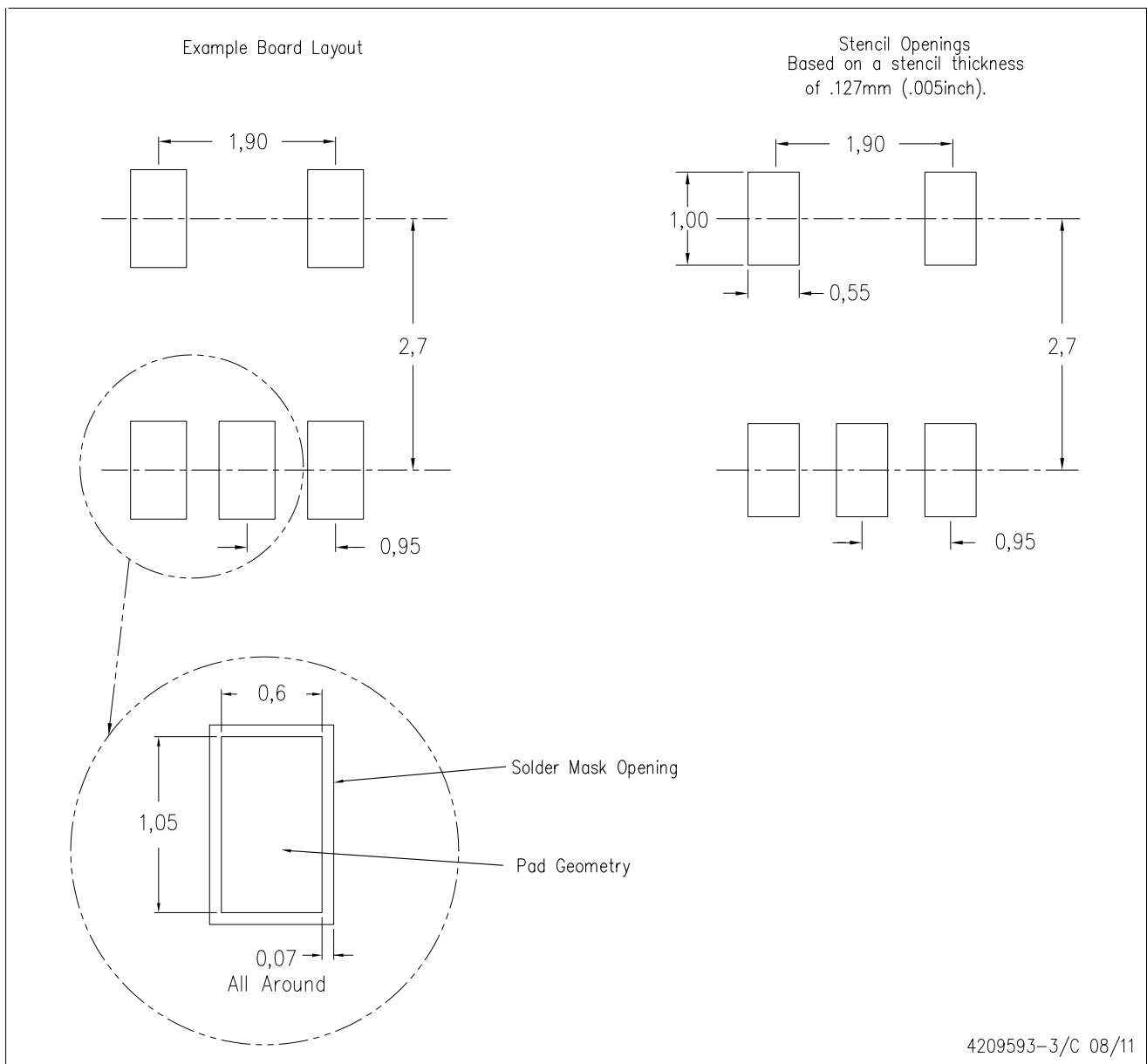
PLASTIC SMALL-OUTLINE PACKAGE



- NOTES:
- A. All linear dimensions are in millimeters.
 - B. This drawing is subject to change without notice.
 - C. Body dimensions do not include mold flash or protrusion. Mold flash and protrusion shall not exceed 0.15 per side.
 - D. Falls within JEDEC MO-178 Variation AA.

DBV (R-PDSO-G5)

PLASTIC SMALL OUTLINE



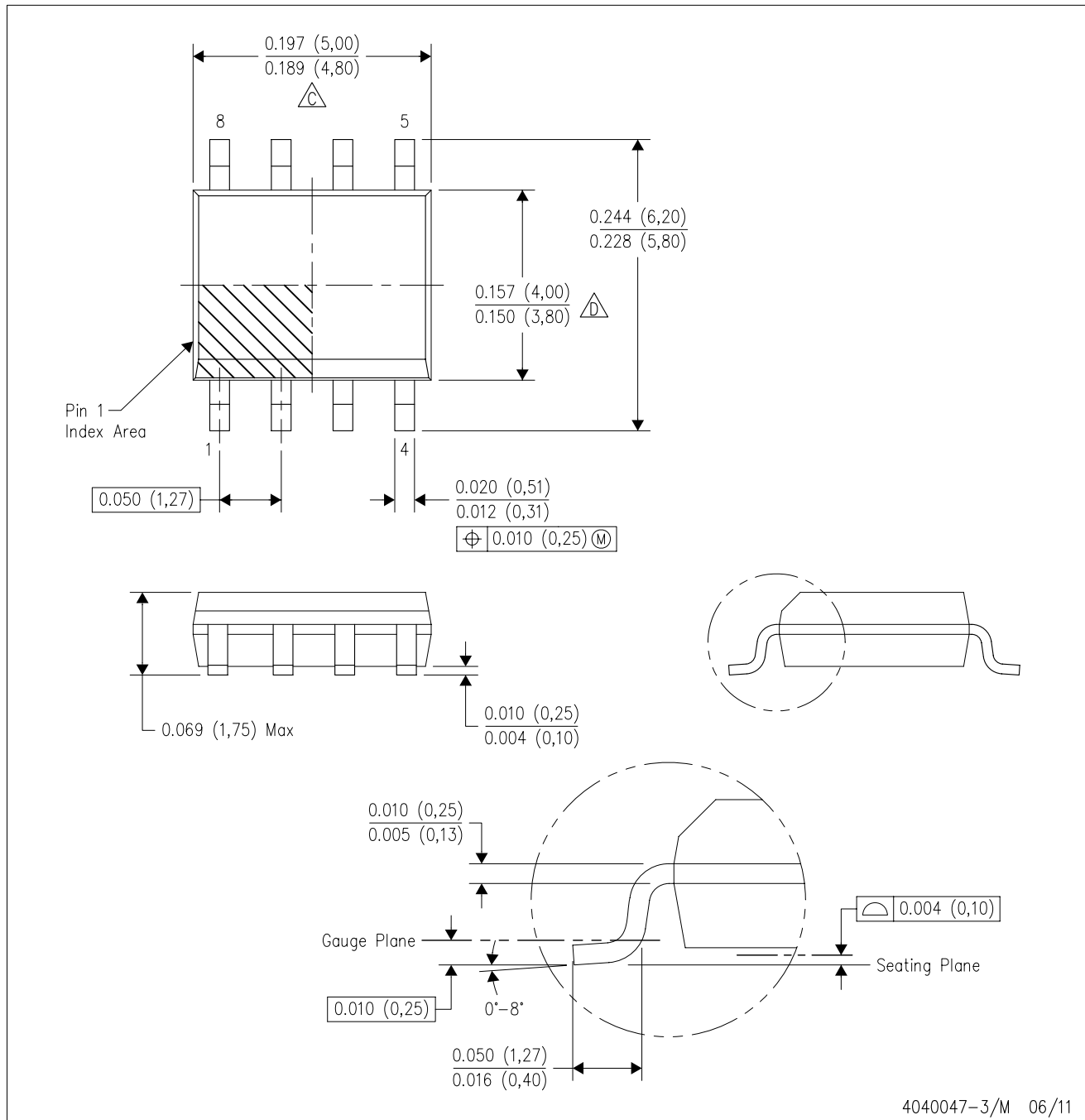
- NOTES:
- A. All linear dimensions are in millimeters.
 - B. This drawing is subject to change without notice.
 - C. Customers should place a note on the circuit board fabrication drawing not to alter the center solder mask defined pad.
 - D. Publication IPC-7351 is recommended for alternate designs.
 - E. Laser cutting apertures with trapezoidal walls and also rounding corners will offer better paste release. Customers should contact their board assembly site for stencil design recommendations. Example stencil design based on a 50% volumetric metal load solder paste. Refer to IPC-7525 for other stencil recommendations.



- NOTES:
- A. All linear dimensions are in millimeters.
 - B. This drawing is subject to change without notice.
 - C. Publication IPC-7351 is recommended for alternate designs.
 - D. Laser cutting apertures with trapezoidal walls and also rounding corners will offer better paste release. Customers should contact their board assembly site for stencil design recommendations. Refer to IPC-7525 for other stencil recommendations.
 - E. Customers should contact their board fabrication site for solder mask tolerances between and around signal pads.

D (R-PDSO-G8)

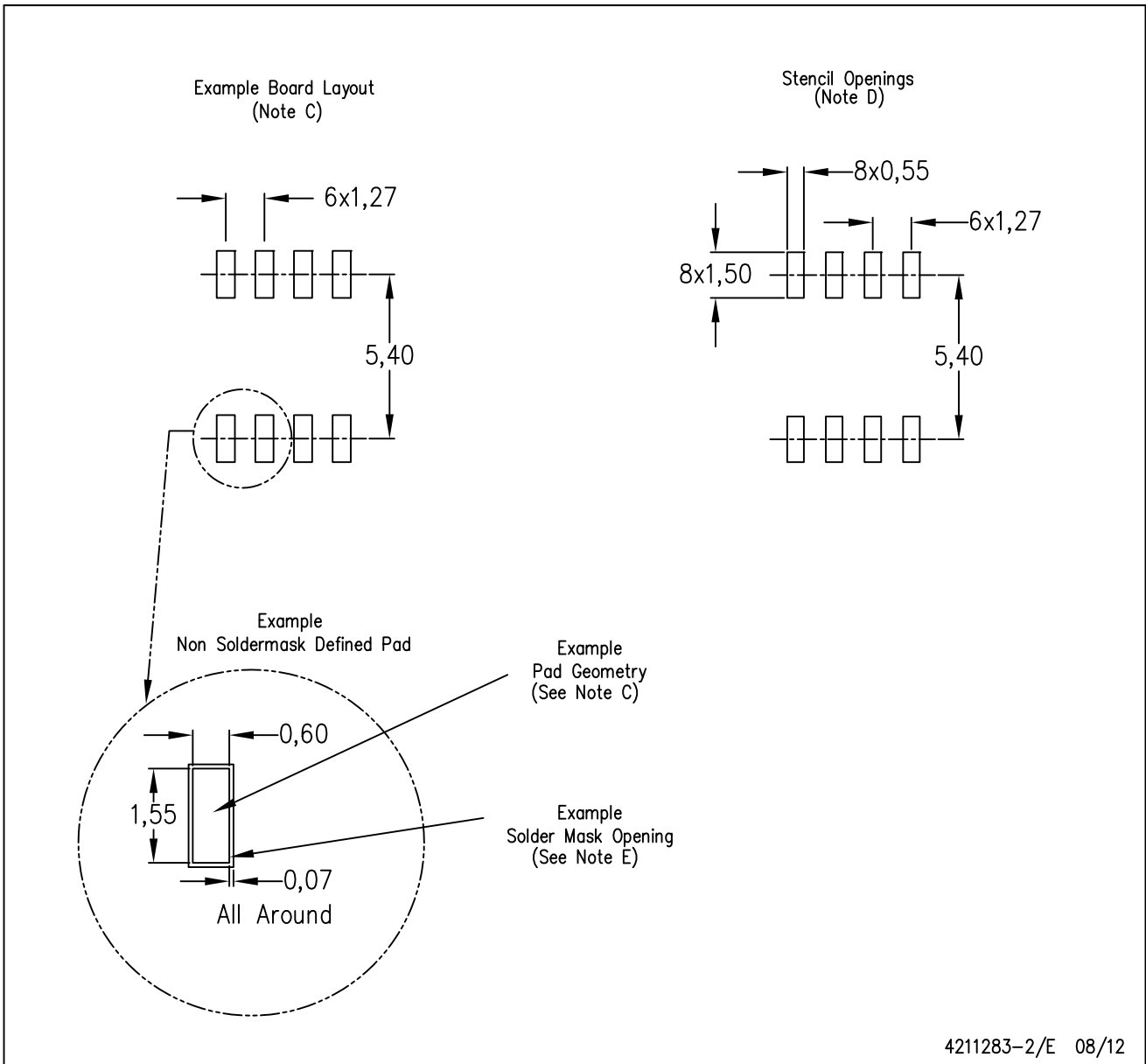
PLASTIC SMALL OUTLINE



- NOTES:
- A. All linear dimensions are in inches (millimeters).
 - B. This drawing is subject to change without notice.
 - C. Body length does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed 0.006 (0,15) each side.
 - D. Body width does not include interlead flash. Interlead flash shall not exceed 0.017 (0,43) each side.
 - E. Reference JEDEC MS-012 variation AA.

D (R-PDSO-G8)

PLASTIC SMALL OUTLINE



- NOTES:
- All linear dimensions are in millimeters.
 - This drawing is subject to change without notice.
 - Publication IPC-7351 is recommended for alternate designs.
 - Laser cutting apertures with trapezoidal walls and also rounding corners will offer better paste release. Customers should contact their board assembly site for stencil design recommendations. Refer to IPC-7525 for other stencil recommendations.
 - Customers should contact their board fabrication site for solder mask tolerances between and around signal pads.

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